

## 800mA, 6MHz 高效降压转换器 采用芯片级封装, 具有 I<sup>2</sup>C™ 兼容接口

查询样片: [TPS62650-Q1](#)

### 特性

- 符合汽车应用要求
- 具有符合 **AEC-Q100** 的下列结果:
  - 器件温度 2 级: **-40°C** 至 **+105°C** 的环境运行温度范围
  - 器件人体模型 (HBM) 静电放电 (ESD) 分类等级 **H2**
  - 器件充电器件模型 (CDM) ESD 分类等级 **C3B**
- **6MHz** 运行时效率为 **86%**
- **38μA** 静态电流
- **2.3V** 至 **5.5V** 的宽  $V_{IN}$  范围
- **6MHz** 稳频运行
- 同类产品中最佳的 负载和线路瞬态
- **±2%** 脉宽调制 (PWM) 直流电压精度
- 自动脉冲频率调制 (PFM) / 脉冲宽度调制 (PWM) 模式切换
- 低纹波轻负载 **PFM**
- 速率高达 **3.4Mbps** 的 **I<sup>2</sup>C** 兼容接口
- 可选引脚输出电压 (**VSEL**)
- 内部软启动, **<150μs** 的启动时间
- 电流过载和热关断保护
- 需要三个表面贴装的外部组件 (一个多层陶瓷电容 (MLCC) 电感器、两个陶瓷电容器)
- 完整的 **1 毫米** 以下组件外形解决方案

- 整体解决方案尺寸 **< 13mm<sup>2</sup>**
- 采用 **9 引脚 NanoFree™ (CSP)** 封装

### 应用范围

- **SmartReflex™** 兼容电源
- **OMAP™** 应用处理器内核电源
- 手机、智能电话
- 微型直流到直流转换器模块

### 说明

TPS62650-Q1 器件是一款针对电池供电便携式应用而进行了优化的高频率同步降压直流到直流转换器。为了满足低功耗应用的要求, TPS62650-Q1 支持高达 **800 mA** 的负载电流, 而且还允许使用小型, 低成本电感器与电容器。

该器件是移动电话以及类似的由单节锂离子电池供电应用的理想选择。借助可调输出电压范围 (可由一个 **I<sup>2</sup>C** 接口调低至 **0.75V**), 此器件支持智能手机和手持计算机内为数字信号处理器 (DSP) 和处理器供电的低压内核电源。

TPS62650-Q1 可在经调节的 **6MHz** 开关频率下运行并在轻负载电流时进入频率优化省电模式, 从而在整个负载电流范围内保持高效率。在关断模式下, 流耗减少至小于 **3.5μA**。

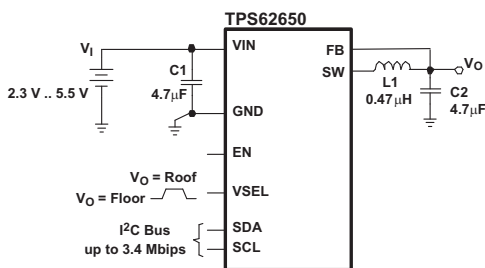


图 1. 典型应用

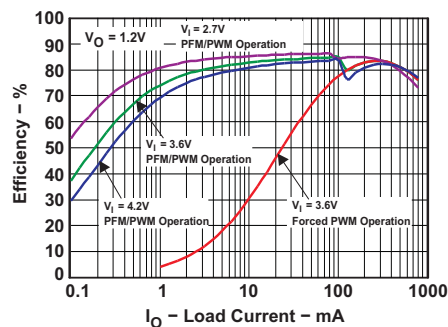


图 2. 效率与负载控制间的关系

此串行接口与标准, 快速/超快速以及高速模式 **I<sup>2</sup>C** 技术规范兼容, 从而实现高达 **3.4Mbps** 的数据传输。这个通信接口用于动态电压缩放, 例如将电压降压至 **12.5mV**, 以设置输出电压, 或者重新设定工作模式 (**PFM/PWM** 或强制 **PWM**)。



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English Data Sheet: [SLVSB62](#)



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

## ORDERING INFORMATION

PART NUMBER	OUTPUT VOLTAGE RANGE	DEFAULT OUTPUT VOLTAGE		I <sup>2</sup> C ADDRESS BITS		PACKAGE	ORDERING	PACKAGE MARKING (CC)
		VSEL0	VSEL1	A2	A1			
TPS62650-Q1 <sup>(1)</sup>	0.75 V to 1.4375 V	1.05 V	1.2 V	0	1	YFF-9	TPS62650TYFFRQ1	Q1

- (1) The following registers bits are set by internal hardware logic and not user programmable through I<sup>2</sup>C:
- (a) VSEL0[7] = 1
  - (b) VSEL1[7] = 1
  - (c) CONTROL1[3:2] = 00

## ABSOLUTE MAXIMUM RATINGS

over operating free-air temperature range (unless otherwise noted)<sup>(1)</sup>

		VALUE		UNIT
		MIN	MAX	
Input Voltage	at VIN, SW <sup>(2)</sup>	−0.3	7	V
	at FB <sup>(2)</sup>	−0.3	3.6	V
	at EN, VSEL, SCL, SDA <sup>(2)</sup>	−0.3	V <sub>I</sub> + 0.3	V
Power dissipation		Internally limited		
Operating ambient temperature, T <sub>A</sub> <sup>(3)</sup>		−40	105	°C
Maximum operating junction Temperature, T <sub>J</sub>			150	°C
Storage temperature range, T <sub>stg</sub>		−65	150	°C
ESD rating <sup>(4)</sup>	Human-body model (HBM) AEC-Q100 Classification Level H2		2	kV
	Charged-device model (CDM) AEC-Q100 Classification Level C3B		750	V

- (1) Stresses beyond those listed under *absolute maximum ratings* may cause permanent damage to the device. These are stress ratings only and functional operation of the device at these or any other conditions beyond those indicated under *recommended operating conditions* is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) All voltage values are with respect to network ground terminal.
- (3) In applications where high power dissipation and/or poor package thermal resistance is present, the maximum ambient temperature may have to be derated. Maximum ambient temperature (T<sub>A(max)</sub>) is dependent on the maximum operating junction temperature (T<sub>J(max)</sub>), the maximum power dissipation of the device in the application (P<sub>D(max)</sub>), and the junction-to-ambient thermal resistance of the part/package in the application (θ<sub>JA</sub>), as given by the following equation: T<sub>A(max)</sub> = T<sub>J(max)</sub> − (θ<sub>JA</sub> × P<sub>D(max)</sub>). To achieve optimum performance, it is recommended to operate the device with a maximum junction temperature of 105°C.
- (4) The human body model is a 100-pF capacitor discharged through a 1.5-kΩ resistor into each pin.

## THERMAL INFORMATION

THERMAL METRIC <sup>(1)</sup>		TPS62650-Q1	UNITS
		YFF	
		9 PINS	
θ <sub>JA</sub>	Junction-to-ambient thermal resistance	107.0	°C/W
θ <sub>JCtop</sub>	Junction-to-case (top) thermal resistance	0.9	
θ <sub>JB</sub>	Junction-to-board thermal resistance	18.1	
ψ <sub>JT</sub>	Junction-to-top characterization parameter	4.0	
ψ <sub>JB</sub>	Junction-to-board characterization parameter	18.0	
θ <sub>JCbot</sub>	Junction-to-case (bottom) thermal resistance	n/a	

- (1) For more information about traditional and new thermal metrics, see the *IC Package Thermal Metrics* application report, [SPRA953](#).

## ELECTRICAL CHARACTERISTICS

Minimum and maximum values are at  $V_I = 2.3\text{V}$  to  $5.5\text{V}$ ,  $V_O = 1.2\text{V}$ ,  $\text{EN} = 1.8\text{V}$ ,  $\text{EN\_DCDC}$  bit = 1, AUTO mode and  $T_A = -40^\circ\text{C}$  to  $105^\circ\text{C}$ ; Circuit of Parameter Measurement Information section (unless otherwise noted). Typical values are at  $V_I = 3.6\text{V}$ ,  $V_O = 1.2\text{V}$ ,  $\text{EN} = 1.8\text{V}$ ,  $\text{EN\_DCDC}$  bit = 1, AUTO mode and  $T_A = 25^\circ\text{C}$  (unless otherwise noted).

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>SUPPLY CURRENT</b>						
$V_I$	Input voltage range		2.3		5.5	V
$I_Q$	Operating quiescent current	$V_I = 3.6\text{V}$ , $I_O = 0\text{mA}$ , $-40^\circ\text{C} \leq T_A \leq 105^\circ\text{C}$ . Device not switching		38	80	$\mu\text{A}$
		$V_I = 3.6\text{V}$ , $I_O = 0\text{mA}$ . PWM mode		5.35		mA
$I_{(SD)}$	Shutdown current	$V_I = 3.6\text{V}$ , $\text{EN} = \text{GND}$ , $\text{EN\_DCDC}$ bit = X, $-40^\circ\text{C} \leq T_A \leq 105^\circ\text{C}$		0.5	10	$\mu\text{A}$
		$V_I = 3.6\text{V}$ , $\text{EN} = V_I$ , $\text{EN\_DCDC}$ bit = 0, $-40^\circ\text{C} \leq T_A \leq 105^\circ\text{C}$		0.5	10	$\mu\text{A}$
UVLO	Undervoltage lockout threshold	Falling		2.05	2.15	V
<b>ENABLE, VSEL, SDA, SCL</b>						
$V_{IH}$	High-level input voltage		0.9			V
$V_{IL}$	Low-level input voltage				0.4	V
$I_{lk}$	Input leakage current	Input tied to GND or $V_I$ , $-40^\circ\text{C} \leq T_A \leq 105^\circ\text{C}$		0.01	0.7	$\mu\text{A}$
<b>POWER SWITCH</b>						
$r_{DS(on)}$	P-channel MOSFET on resistance	$V_I = V_{(GS)} = 3.6\text{V}$		255		m $\Omega$
		$V_I = V_{(GS)} = 2.5\text{V}$		335		
$I_{lk}$	P-channel leakage current, PMOS	$V_{(DS)} = 5.5\text{V}$ , $-40^\circ\text{C} \leq T_A \leq 105^\circ\text{C}$			1	$\mu\text{A}$
$r_{DS(on)}$	N-channel MOSFET on resistance	$V_I = V_{(GS)} = 3.6\text{V}$		140		m $\Omega$
		$V_I = V_{(GS)} = 2.5\text{V}$		200		
$I_{lk}$	N-channel leakage current, NMOS	$V_{(DS)} = 5.5\text{V}$ , $-40^\circ\text{C} \leq T_A \leq 105^\circ\text{C}$			1	$\mu\text{A}$
$r_{DIS}$	Discharge resistor for power-down sequence			15	50	$\Omega$
	P-MOS current limit	$2.3\text{V} \leq V_I \leq 4.8\text{V}$ . Open loop	1200	1500	1850	mA
	Input current limit under short-circuit conditions	$V_O = 0\text{V}$		11		mA
	Thermal shutdown			140		$^\circ\text{C}$
	Thermal shutdown hysteresis			15		$^\circ\text{C}$
<b>OSCILLATOR</b>						
$f_{SW}$	Oscillator frequency	$I_O = 0\text{mA}$ . PWM mode, $T_A = 25^\circ\text{C}$	5.4	6	6.6	MHz
		$I_O = 0\text{mA}$ . PWM mode, $-40^\circ\text{C} \leq T_A \leq 105^\circ\text{C}$	5.2	6	6.8	

## ELECTRICAL CHARACTERISTICS (continued)

Minimum and maximum values are at  $V_I = 2.3\text{V}$  to  $5.5\text{V}$ ,  $V_O = 1.2\text{V}$ ,  $\text{EN} = 1.8\text{V}$ ,  $\text{EN\_DCDC}$  bit = 1, AUTO mode and  $T_A = -40^\circ\text{C}$  to  $105^\circ\text{C}$ ; Circuit of Parameter Measurement Information section (unless otherwise noted). Typical values are at  $V_I = 3.6\text{V}$ ,  $V_O = 1.2\text{V}$ ,  $\text{EN} = 1.8\text{V}$ ,  $\text{EN\_DCDC}$  bit = 1, AUTO mode and  $T_A = 25^\circ\text{C}$  (unless otherwise noted).

PARAMETER			TEST CONDITIONS	MIN	TYP	MAX	UNIT
OUTPUT							
V <sub>O</sub>	Regulated DC output voltage accuracy	TPS62650-Q1/1	2.3 V ≤ V <sub>I</sub> ≤ 5.5 V, 0 mA ≤ I <sub>O(DC)</sub> ≤ 800 mA V <sub>O</sub> = 0.75 V, 1.05 V, 1.20 V, 1.4375 V (TPS62650-Q1) PWM operation	-4%		4%	
			T <sub>A</sub> = 85°C 2.3 V ≤ V <sub>I</sub> ≤ 5.5 V, 0 mA ≤ I <sub>O(DC)</sub> ≤ 800 mA V <sub>O</sub> = 0.75 V, 1.05 V, 1.20 V, 1.4375 V (TPS62650-Q1) PWM operation	-2%		2%	
			2.3 V ≤ V <sub>I</sub> ≤ 5.5 V, 0 mA ≤ I <sub>O(DC)</sub> ≤ 800 mA V <sub>O</sub> = 0.75 V, 1.05 V, 1.20 V, 1.4375 V (TPS62650-Q1) PFM/PWM Operation	-4%		4%	
	Regulated DC output voltage temperature drift	V <sub>I</sub> = 3.6 V, V <sub>O</sub> = 1.20 V, I <sub>O(DC)</sub> = 50 mA -40°C ≤ T <sub>A</sub> ≤ 105°C. PWM operation	-0.5%		+0.5%		
	Line regulation	V <sub>I</sub> = V <sub>O</sub> + 0.5 V (min 2.3 V) to 5.5 V, I <sub>O(DC)</sub> = 200 mA		0.13		%/V	
	Load regulation	I <sub>O(DC)</sub> = 0 mA to 800 mA		-0.00046		%/mA	
Feedback input resistance					480		kΩ
ΔV <sub>O</sub>	Power-save mode ripple voltage		V <sub>O</sub> = 1.05 V, VSEL = GND, I <sub>O(DC)</sub> = 1 mA PFM operation		16		mV <sub>PP</sub>
			V <sub>O</sub> = 1.20 V, VSEL = V <sub>I</sub> , I <sub>O(DC)</sub> = 1 mA PFM operation		16		mV <sub>PP</sub>
DAC							
Resolution		TPS62650-Q1			6		Bits
Differential nonlinearity			Specified monotonic by design			±0.4	LSB
TIMING							
Setup Time Between Rising EN and Start of I <sup>2</sup> C Stream		TPS62650-Q1/1			50		μs
V <sub>O</sub>	Output voltage settling time	TPS62650-Q1/1	From min to max output voltage, I <sub>O(DC)</sub> = 500 mA, VSEL = V <sub>I</sub> , PWM operation		12		μs
Start-up time		TPS62650-Q1/1	Time from active EN to V <sub>O</sub> V <sub>O</sub> = 1.2 V, I <sub>O</sub> = 0 mA, PWM operation		125		μs
			Time from active EN to V <sub>O</sub> V <sub>O</sub> = 1.05 V, I <sub>O</sub> = 0 mA, PFM operation		120		

## I<sup>2</sup>C INTERFACE TIMING CHARACTERISTICS<sup>(1)</sup>

PARAMETER		TEST CONDITIONS	MIN	MAX	UNIT
$f_{\text{SCL}}$	SCL Clock Frequency	Standard mode		100	kHz
		Fast mode		400	kHz
		Fast mode plus		1	MHz
		High-speed mode (write operation), $C_B = 100\text{pF}$ max		3.4	MHz
		High-speed mode (read operation), $C_B = 100\text{pF}$ max		3.4	MHz
		High-speed mode (write operation), $C_B = 400\text{pF}$ max		1.7	MHz
		High-speed mode (read operation), $C_B = 400\text{pF}$ max		1.7	MHz
$t_{\text{BUF}}$	Bus Free Time Between a STOP and START Condition	Standard mode	4.7		$\mu\text{s}$
		Fast mode	1.3		$\mu\text{s}$
		Fast mode plus	0.5		$\mu\text{s}$
$t_{\text{HD}}$ , $t_{\text{STA}}$	Hold Time (Repeated) START Condition	Standard mode	4		$\mu\text{s}$
		Fast mode	600		ns
		Fast mode plus	260		ns
		High-speed mode	160		ns

(1) Specified by design. Not tested in production.

**I<sup>2</sup>C INTERFACE TIMING CHARACTERISTICS (continued)**

PARAMETER		TEST CONDITIONS	MIN	MAX	UNIT
t <sub>LOW</sub>	LOW Period of the SCL Clock	Standard mode	4.7		μs
		Fast mode	1.3		μs
		Fast mode plus	0.5		μs
		High-speed mode, C <sub>B</sub> – 100 pF max	160		ns
		High-speed mode, C <sub>B</sub> – 400 pF max	320		ns
t <sub>HIGH</sub>	HIGH Period of the SCL Clock	Standard mode	4		μs
		Fast mode	600		ns
		Fast mode plus	260		ns
		High-speed mode, C <sub>B</sub> – 100 pF max	60		ns
		High-speed mode, C <sub>B</sub> – 400 pF max	120		ns
t <sub>SU</sub> , t <sub>STA</sub>	Setup Time for a Repeated START Condition	Standard mode	4.7		μs
		Fast mode	600		ns
		Fast mode plus	260		ns
		High-speed mode	160		ns
t <sub>SU</sub> , t <sub>DAT</sub>	Data Setup Time	Standard mode	250		ns
		Fast mode	100		ns
		Fast mode plus	50		ns
		High-speed mode	10		ns
t <sub>HD</sub> , t <sub>DAT</sub>	Data Hold Time	Standard mode	0	3.45	μs
		Fast mode	0	0.9	μs
		Fast mode plus	0		μs
		High-speed mode, C <sub>B</sub> – 100 pF max	0	70	ns
		High-speed mode, C <sub>B</sub> – 400 pF max	0	150	ns
t <sub>RCL</sub>	Rise Time of SCL Signal	Standard mode	20 + 0.1 C <sub>B</sub>	1000	ns
		Fast mode	20 + 0.1 C <sub>B</sub>	300	ns
		Fast mode plus		120	ns
		High-speed mode, C <sub>B</sub> – 100 pF max	10	40	ns
		High-speed mode, C <sub>B</sub> – 400 pF max	20	80	ns
t <sub>RCL1</sub>	Rise Time of SCL Signal After a Repeated START Condition and After an Acknowledge BIT	Standard mode	20 + 0.1 C <sub>B</sub>	1000	ns
		Fast mode	20 + 0.1 C <sub>B</sub>	300	ns
		Fast mode plus		120	ns
		High-speed mode, C <sub>B</sub> – 100 pF max	10	80	ns
		High-speed mode, C <sub>B</sub> – 400 pF max	20	160	ns
t <sub>FCL</sub>	Fall Time of SCL Signal	Standard mode	20 + 0.1 C <sub>B</sub>	300	ns
		Fast mode	20 + 0.1 C <sub>B</sub>	300	ns
		Fast mode plus		120	ns
		High-speed mode, C <sub>B</sub> – 100 pF max	10	40	ns
		High-speed mode, C <sub>B</sub> – 400 pF max	20	80	ns
t <sub>RDA</sub>	Rise Time of SDA Signal	Standard mode	20 + 0.1 C <sub>B</sub>	1000	ns
		Fast mode	20 + 0.1 C <sub>B</sub>	300	ns
		Fast mode plus		120	ns
		High-speed mode, C <sub>B</sub> – 100 pF max	10	80	ns
		High-speed mode, C <sub>B</sub> – 400 pF max	20	160	ns

**I<sup>2</sup>C INTERFACE TIMING CHARACTERISTICS (continued)**

PARAMETER		TEST CONDITIONS	MIN	MAX	UNIT
$t_{FDA}$ Fall Time of SDA Signal		Standard mode	$20 + 0.1 C_B$	300	ns
		Fast mode	$20 + 0.1 C_B$	300	ns
		Fast mode plus		120	ns
		High-speed mode, $C_B = 100$ pF max	10	80	ns
		High-speed mode, $C_B = 400$ pF max	20	160	ns
$t_{SU}, t_{STO}$ Setup Time of STOP Condition		Standard mode	4		$\mu$ s
		Fast mode	600		ns
		Fast mode plus	260		ns
		High-Speed mode	160		ns
$C_B$ Capacitive Load for SDA and SCL		Standard mode		400	pF
		Fast mode		400	pF
		Fast mode plus		550	pF
		High-Speed mode		400	pF

[illegible]

The diagram illustrates the timing relationships between the SDA (Serial Data) and SCL (Serial Clock) signals. The SDA signal is shown as a multi-bit data stream, and the SCL signal is shown as a periodic clock signal. Key timing parameters are labeled:

- $t_{fDA}$ : SDA fall time from high to low.
- $t_{rDA}$ : SDA rise time from low to high.
- $t_{su;STA}$ : SDA setup time before SCL sampling edge.
- $t_{hd;STA}$ : SDA hold time after SCL sampling edge.
- $t_{hd;DAT}$ : SDA hold time after SCL data output edge.
- $t_{su;DAT}$ : SDA setup time before SCL data output edge.
- $t_{su;STO}$ : SDA setup time before SCL stop edge.
- $t_{rCL1}$ : SCL rise time from low to high.
- $t_{fCL}$ : SCL fall time from high to low.
- $t_{HIGH}$ : SCL high pulse width.
- $t_{LOW}$ : SCL low pulse width.

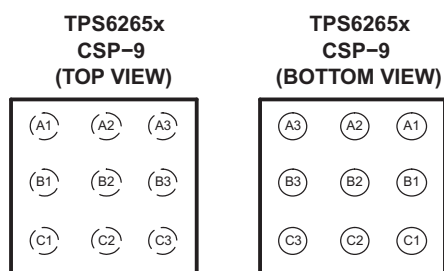
Legend:

- $\text{MCS Current Source Pull-Up}$  (represented by a trapezoidal waveform)
- $R_{(P)} \text{ Resistor Pull-Up}$  (represented by a triangular waveform)

Note A: First rising edge of the SCLH signal after Sr and after each acknowledge bit.

### Figure 4. Serial Interface Timing Diagram for HS-Mode

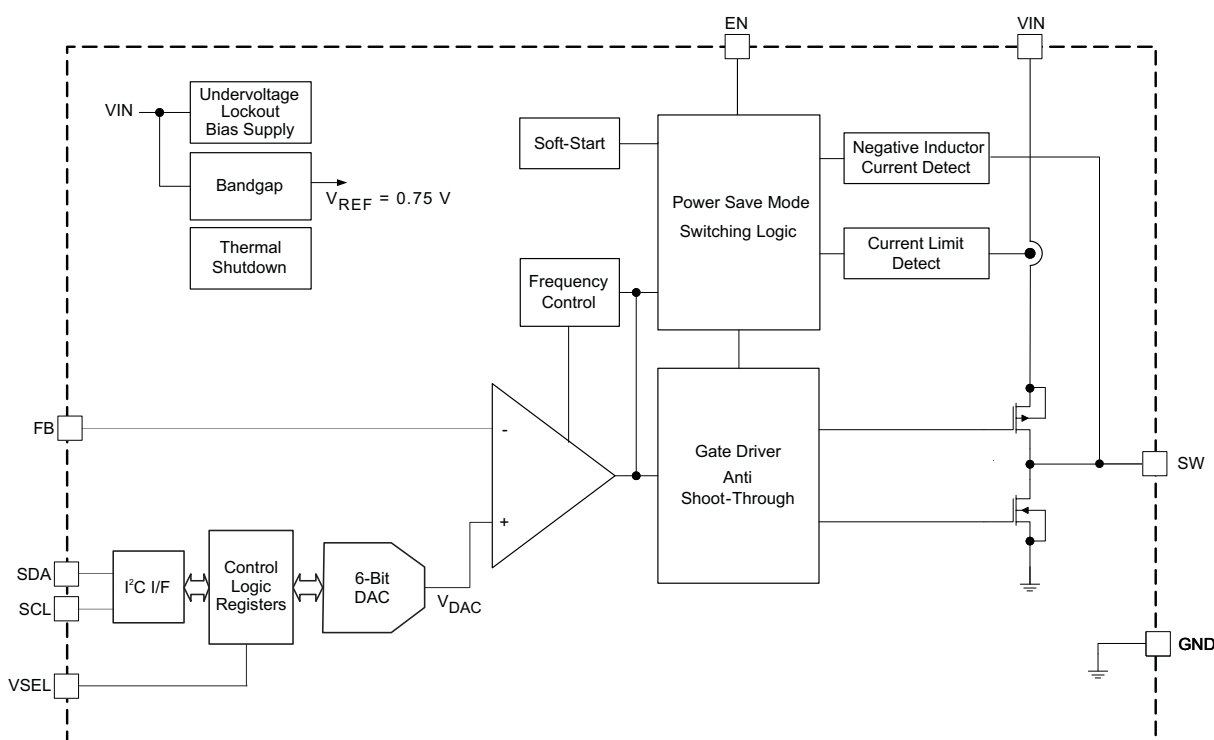
## PIN ASSIGNMENTS



## TERMINAL FUNCTIONS

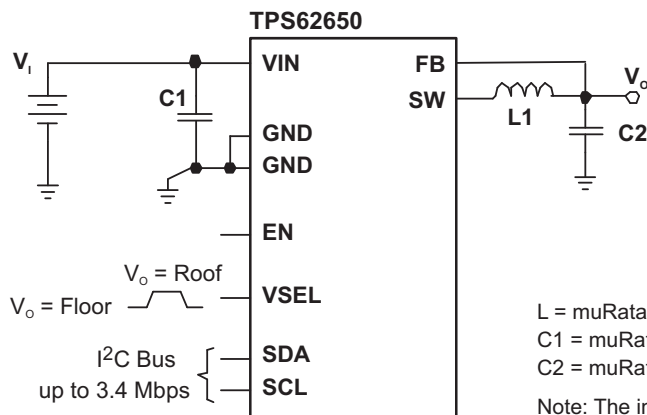
TERMINAL		I/O	DESCRIPTION
NAME	NO.		
VIN	A2	I	This is the input voltage pin of the device. Connect directly to the input bypass capacitor.
EN	B3	I	This is the enable pin of the device. Connect this pin to ground forces the device into shutdown mode. Pulling this pin to $V_I$ enables the device. On the rising edge of the enable pin, all the registers are reset with their default values. This pin must not be left floating and must be terminated.
VSEL	A1	I	VSEL signal is primarily used to scale the output voltage and to set the TPS62650-Q1 operation between active mode (VSEL=HIGH) and sleep mode (VSEL=LOW). The mode of operation can also be adapted by I <sup>2</sup> C settings. This pin must not be left floating and must be terminated.
SDA	A3	I/O	Serial interface address/data line.
SCL	B2	I	Serial interface clock line.
FB	C1	I	Output feedback sense input. Connect FB to the converter output.
GND	C2, C3		Ground.
SW	B1	I/O	This is the switch pin of the converter and connected to the drain of the internal power MOSFETs.

## FUNCTIONAL BLOCK DIAGRAM





## PARAMETER MEASUREMENT INFORMATION



L = muRata LQM21PN1R0NGR

C1 = muRata GRM155R60J475M (4.7μF, 6.3V, 0402, X5R)

C2 = muRata GRM155R60J475M (4.7μF, 6.3V, 0402, X5R)

Note: The internal registers are set to their default values

## TYPICAL CHARACTERISTICS

### Table of Graphs

			FIGURE
$\eta$	Efficiency	vs. Output current	5, 6, 7, 8
		vs. Input voltage	9
V <sub>O</sub>	Peak-to-peak output ripple voltage	vs. Output Current	10, 11, 12, 13
	DC output voltage	vs. Output current	14, 15, 16, 17
	Measured output voltage	vs. Ambient temperature	18, 19
	Measured output voltage	vs. DAC target output voltage	20
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I <sub>SD</sub>	Shutdown current	vs. Input voltage	23
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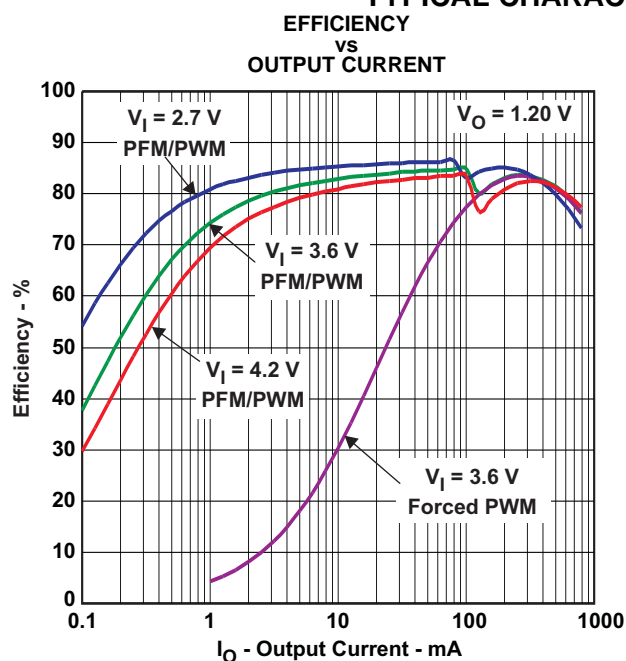
**TYPICAL CHARACTERISTICS (continued)**

Figure 5.

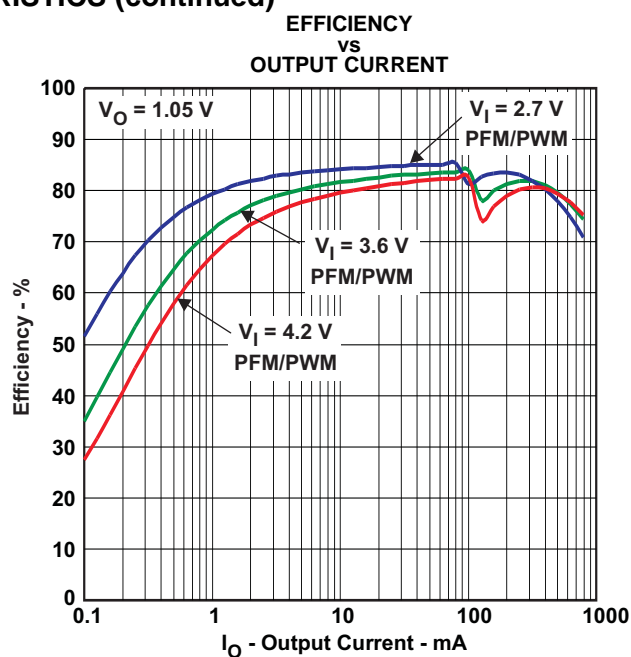


Figure 6.

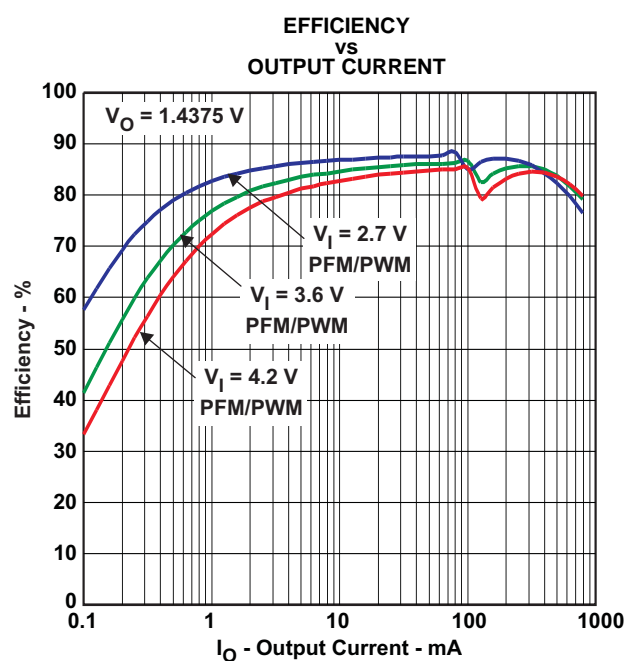


Figure 7.

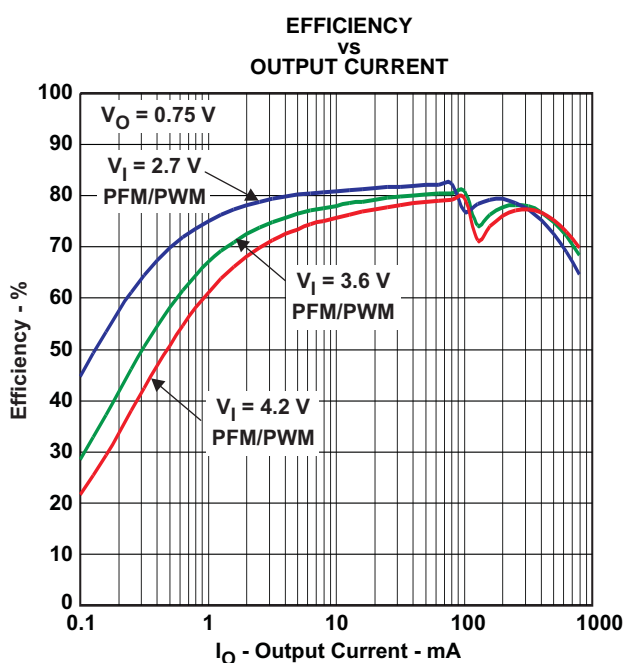
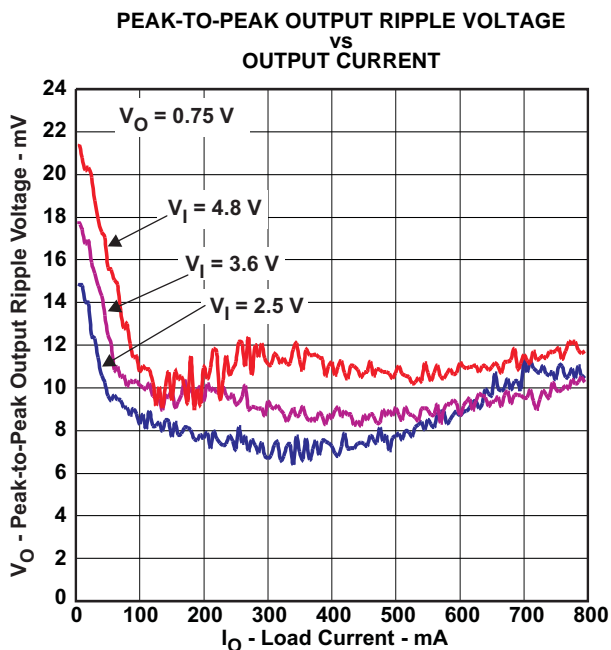
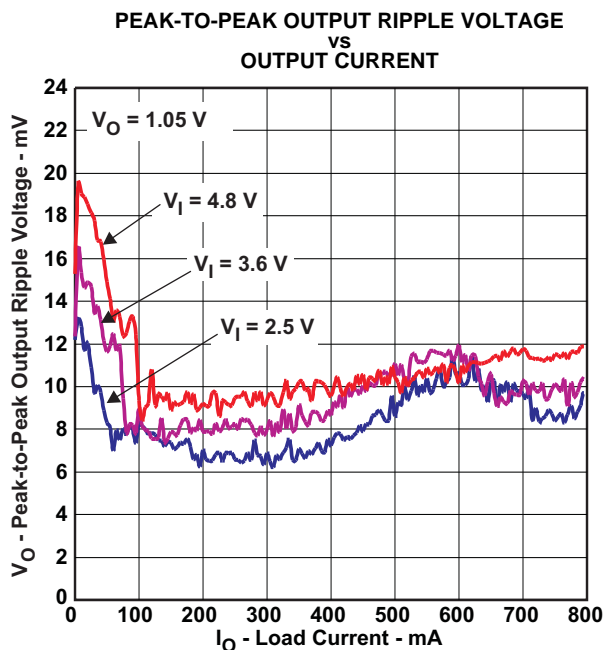
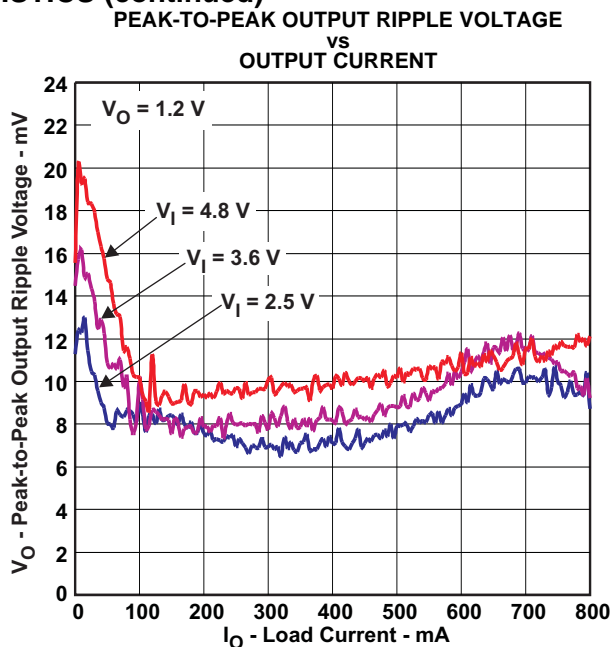
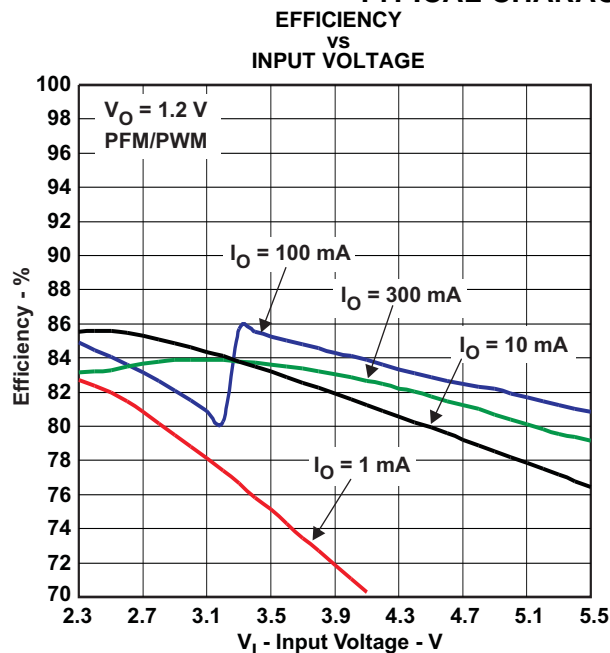


Figure 8.

# TYPICAL CHARACTERISTICS (continued)



**TYPICAL CHARACTERISTICS (continued)**

**PEAK-TO-PEAK OUTPUT RIPPLE VOLTAGE  
vs  
OUTPUT CURRENT**

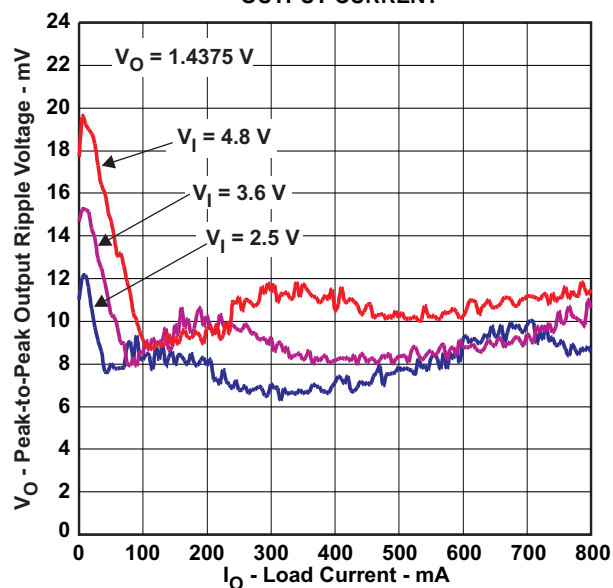


Figure 13.

**DC OUTPUT VOLTAGE  
vs  
OUTPUT CURRENT**

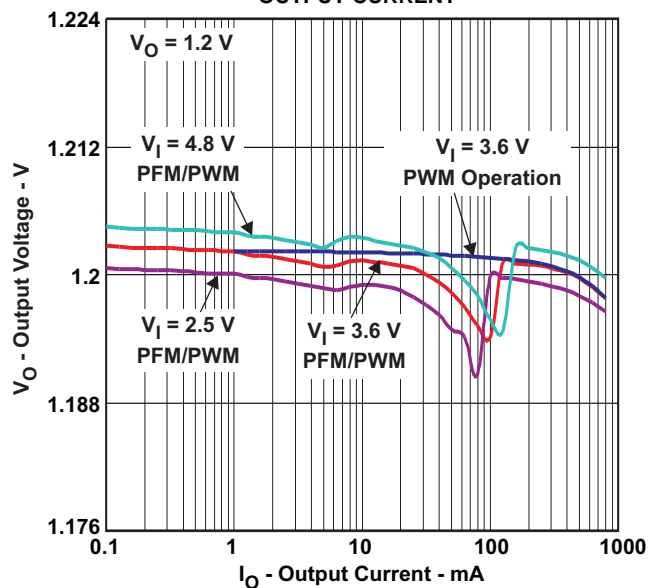


Figure 14.

**DC OUTPUT VOLTAGE  
vs  
OUTPUT CURRENT**

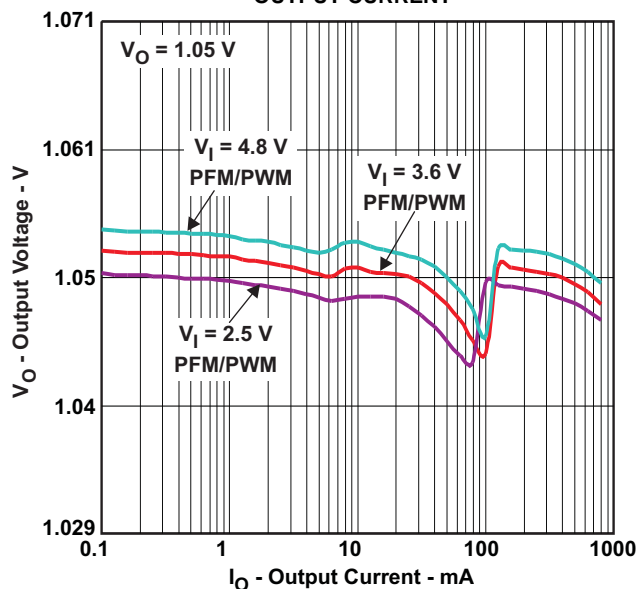


Figure 15.

**DC OUTPUT VOLTAGE  
vs  
OUTPUT CURRENT**

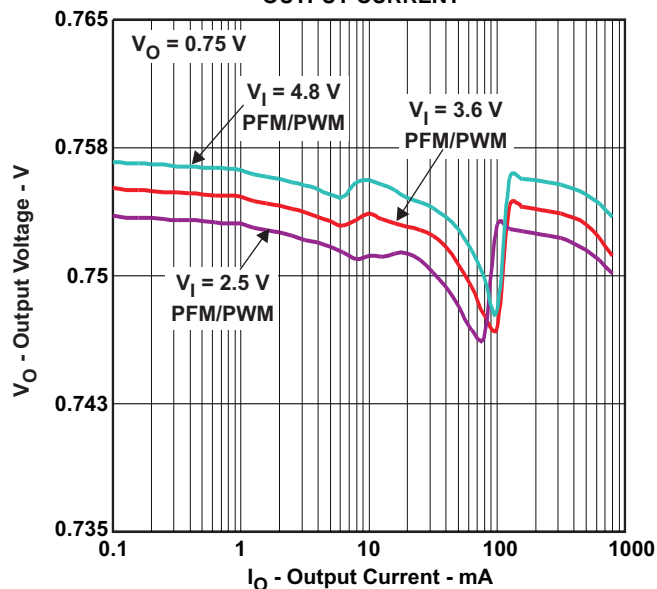


Figure 16.

# TYPICAL CHARACTERISTICS (continued)

DC OUTPUT VOLTAGE  
vs  
OUTPUT CURRENT

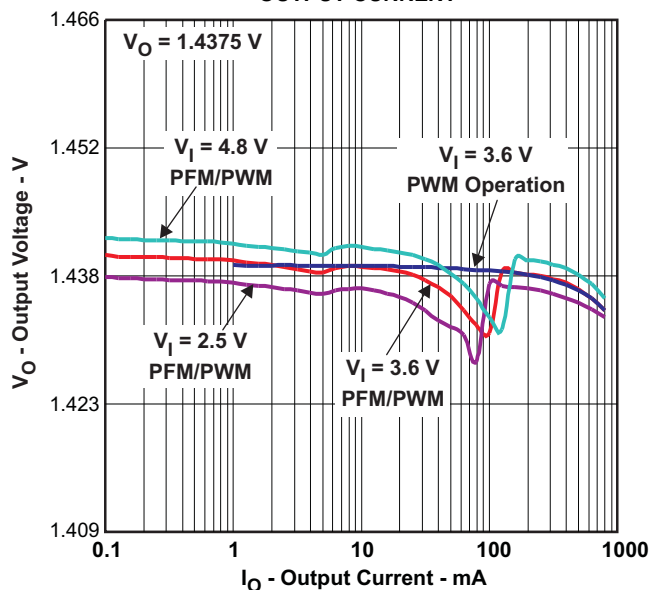


Figure 17.

DC OUTPUT VOLTAGE  
vs  
AMBIENT TEMPERATURE

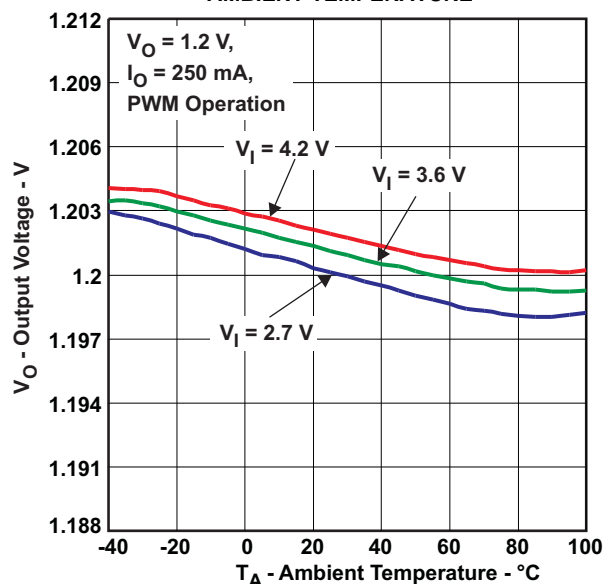


Figure 18.

DC OUTPUT VOLTAGE  
vs  
AMBIENT TEMPERATURE

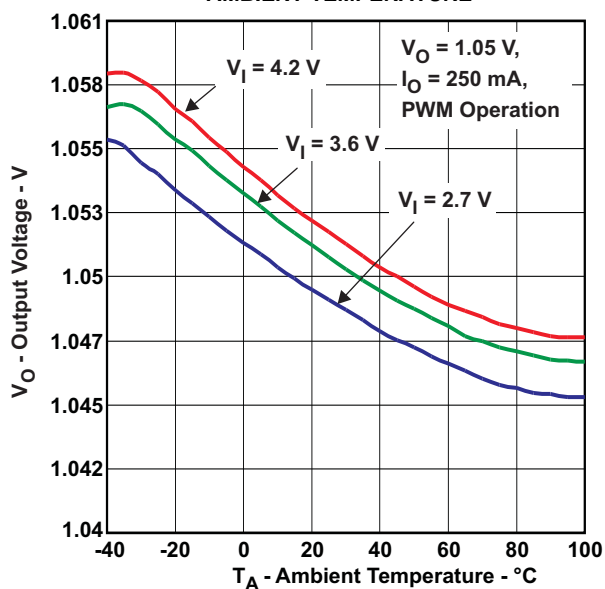


Figure 19.

MEASURED OUTPUT VOLTAGE  
vs  
DAC TARGET OUTPUT VOLTAGE

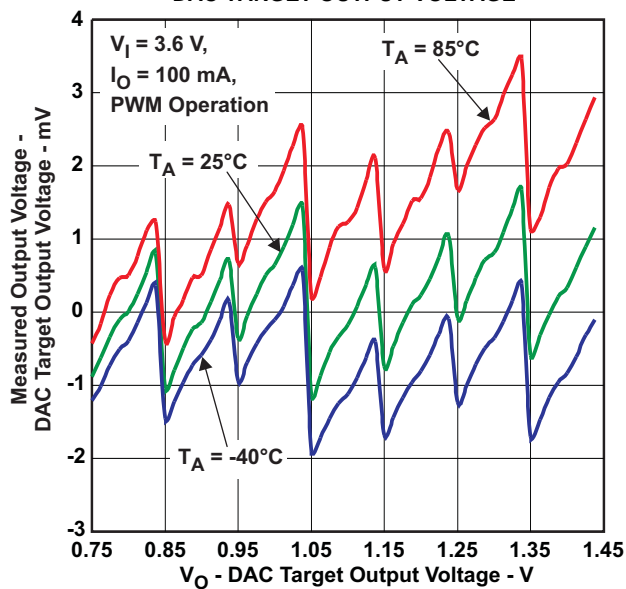


Figure 20.

## TYPICAL CHARACTERISTICS (continued)

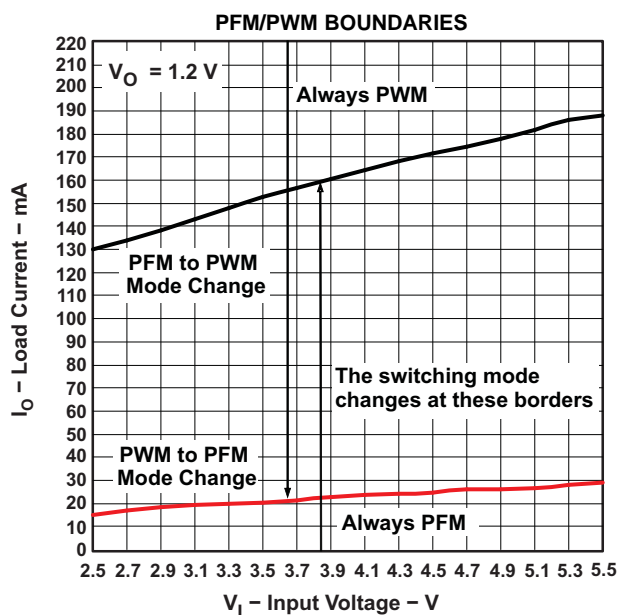


Figure 21.

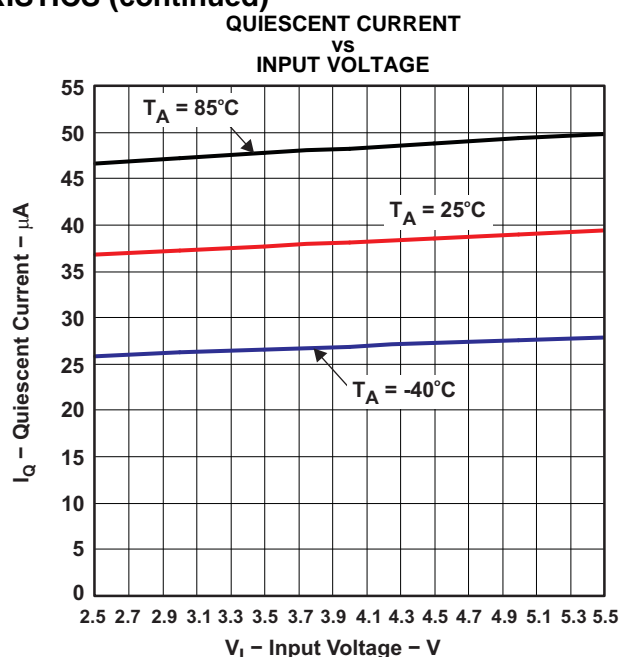


Figure 22.

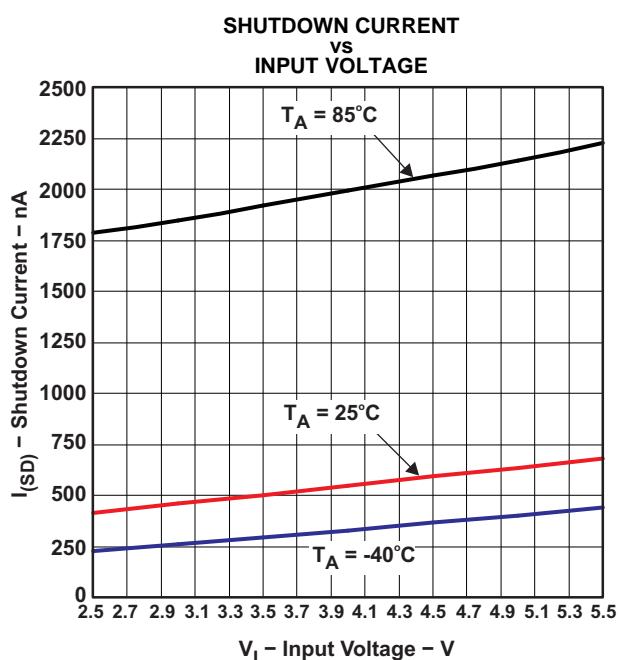


Figure 23.

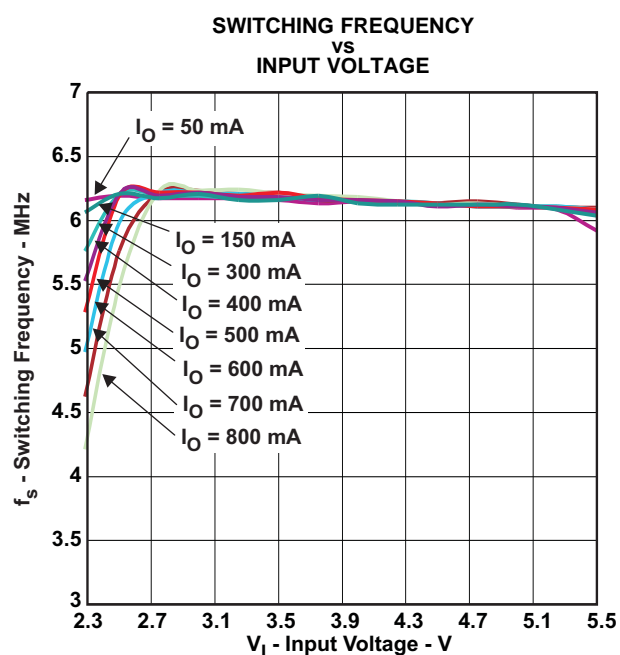


Figure 24.

# TYPICAL CHARACTERISTICS (continued)

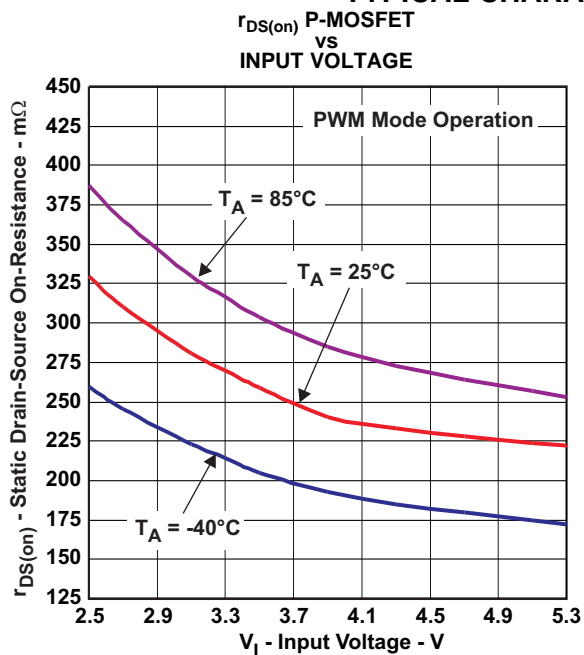


Figure 25.

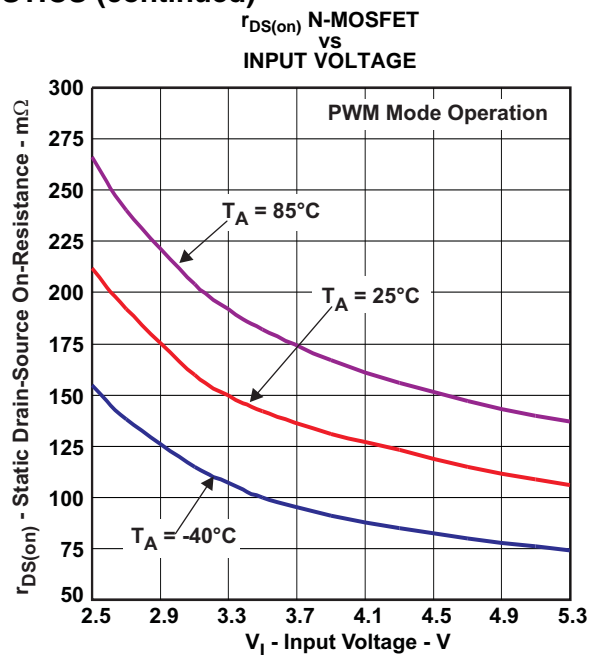


Figure 26.

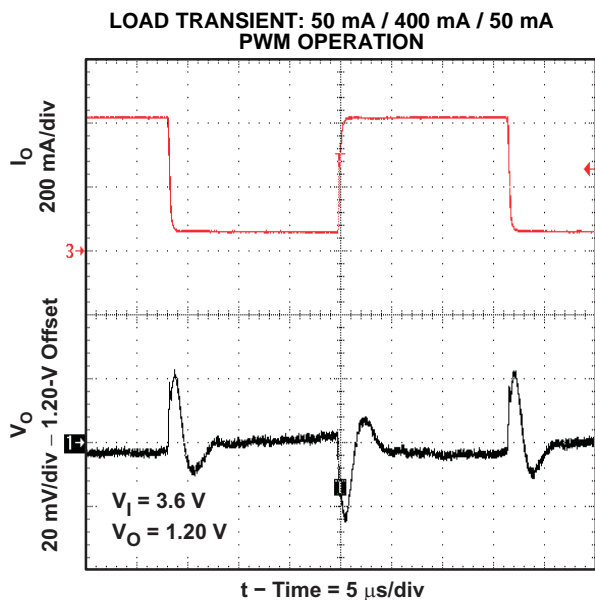


Figure 27.

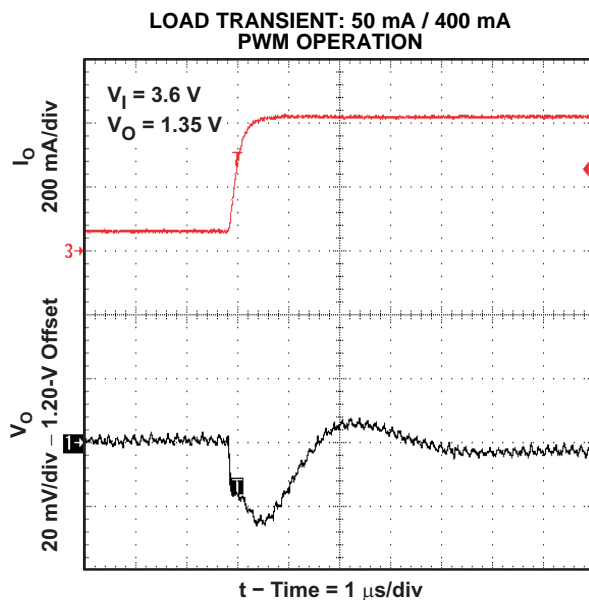


Figure 28.

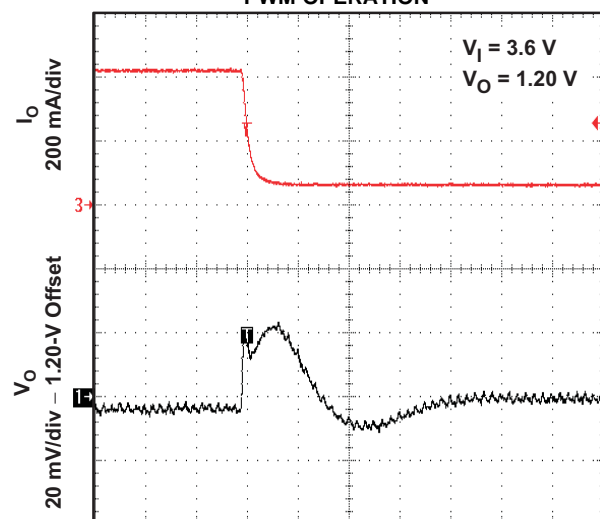
**TYPICAL CHARACTERISTICS (continued)**
**LOAD TRANSIENT: 400 mA / 50 mA**  
**PWM OPERATION**


Figure 29.

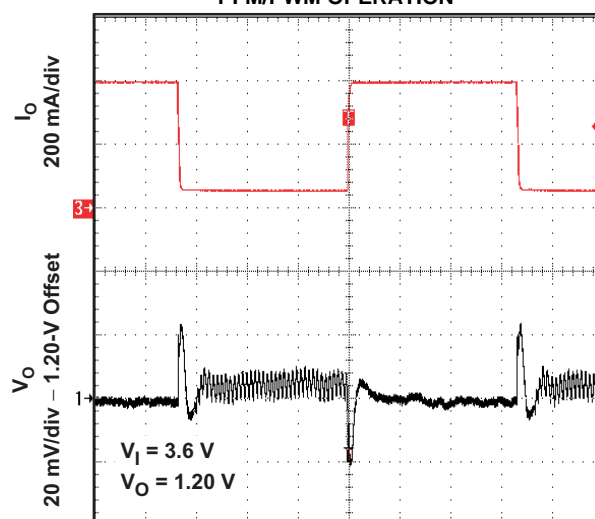
**LOAD TRANSIENT: 50 mA / 400 mA / 50 mA**  
**PFM/PWM OPERATION**


Figure 30.

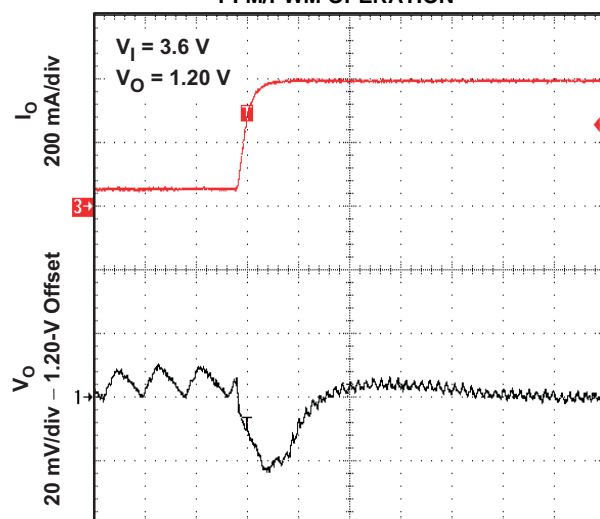
**LOAD TRANSIENT: 50 mA / 400 mA**  
**PFM/PWM OPERATION**


Figure 31.

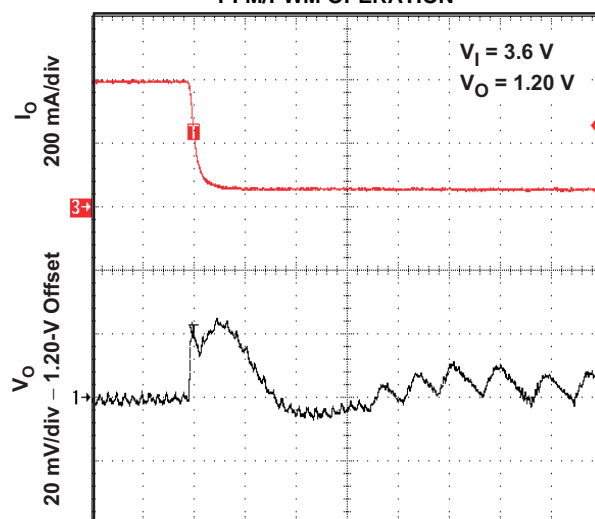
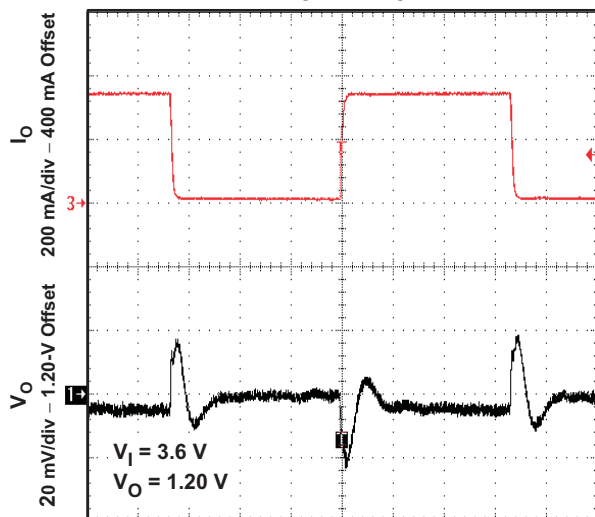
**LOAD TRANSIENT: 400 mA / 50 mA**  
**PFM/PWM OPERATION**


Figure 32.



## TYPICAL CHARACTERISTICS (continued)

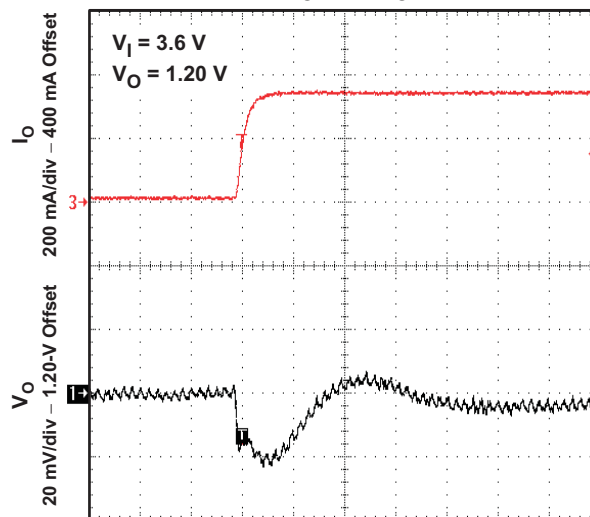
LOAD TRANSIENT: 400 mA / 750 mA / 400 mA  
PWM OPERATION



t – Time = 5  $\mu$ s/div

Figure 33.

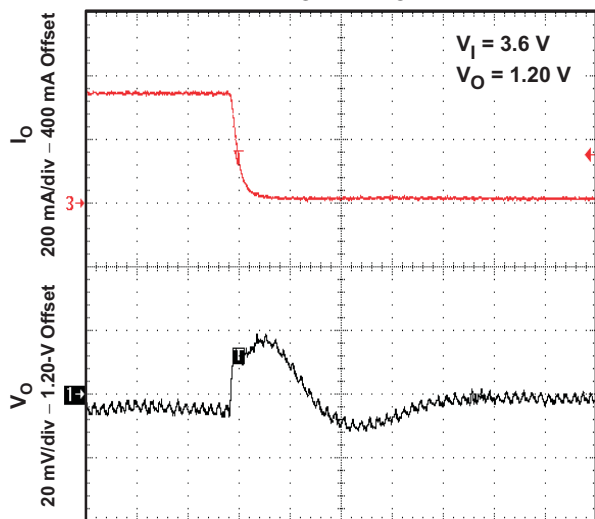
LOAD TRANSIENT: 400 mA / 750 mA  
PWM OPERATION



t – Time = 1  $\mu$ s/div

Figure 34.

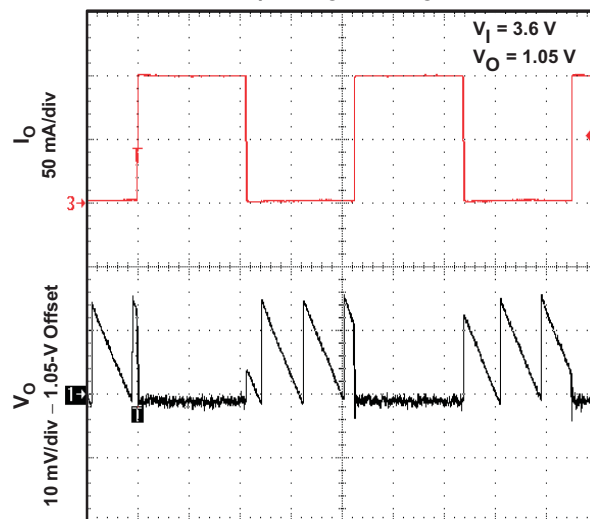
LOAD TRANSIENT: 750 mA / 400 mA  
PWM OPERATION



t – Time = 1  $\mu$ s/div

Figure 35.

LOAD TRANSIENT: 5 mA / 100 mA / 5 mA  
PFM/PWM OPERATION



t – Time = 250  $\mu$ s/div

Figure 36.

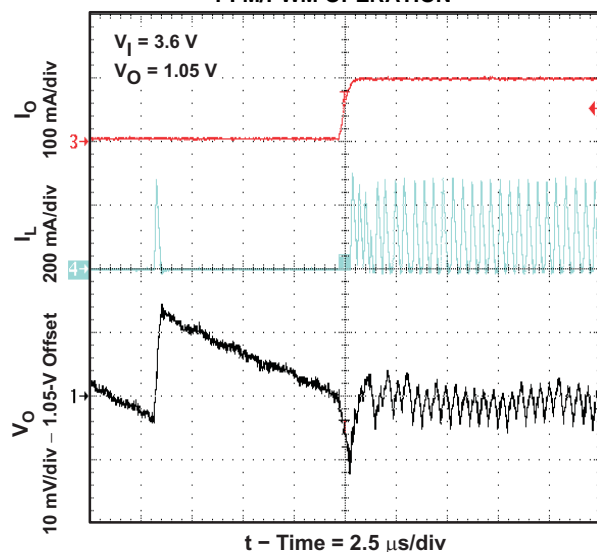
**TYPICAL CHARACTERISTICS (continued)****LOAD TRANSIENT: 5 mA / 100 mA  
PFM/PWM OPERATION**

Figure 37.

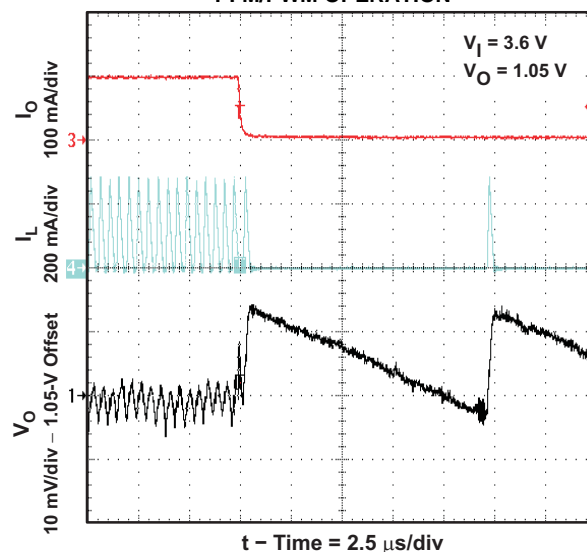
**LOAD TRANSIENT: 100 mA / 5 mA  
PFM/PWM OPERATION**

Figure 38.

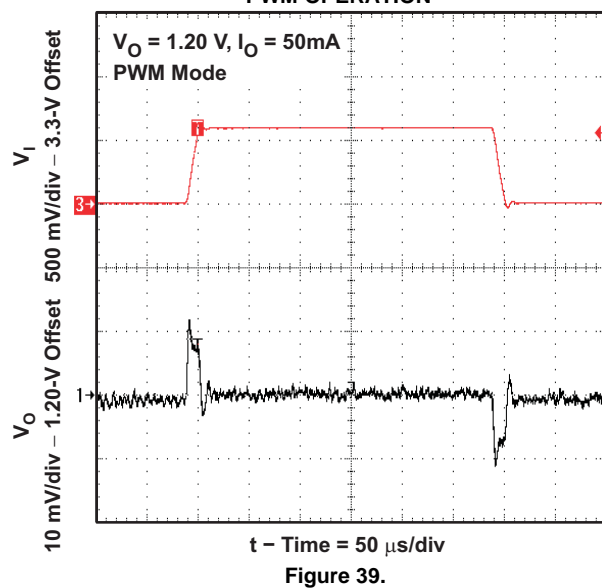
**LINE TRANSIENT  
PWM OPERATION**

Figure 39.

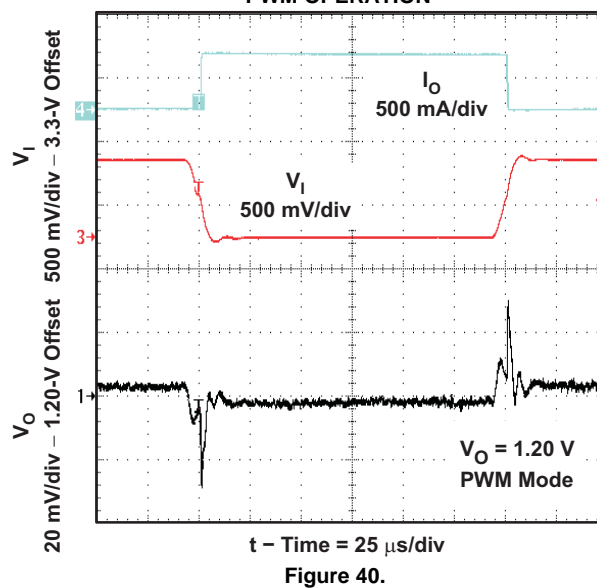
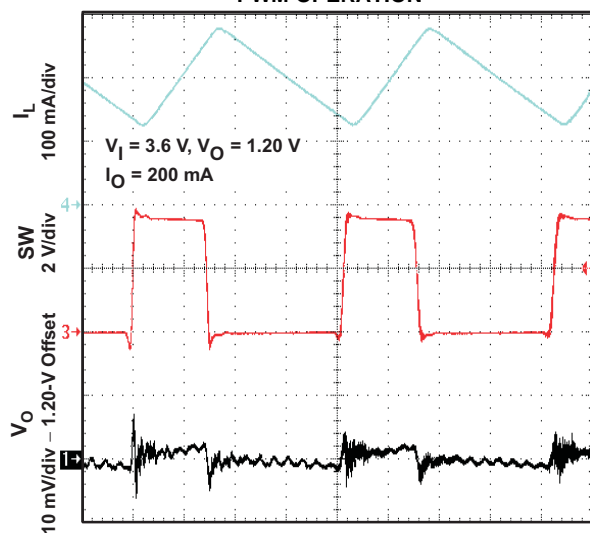
**COMBINED LINE/LOAD TRANSIENT  
(3.3 V TO 3.9 V, 400 mA TO 800 mA)  
PWM OPERATION**

Figure 40.

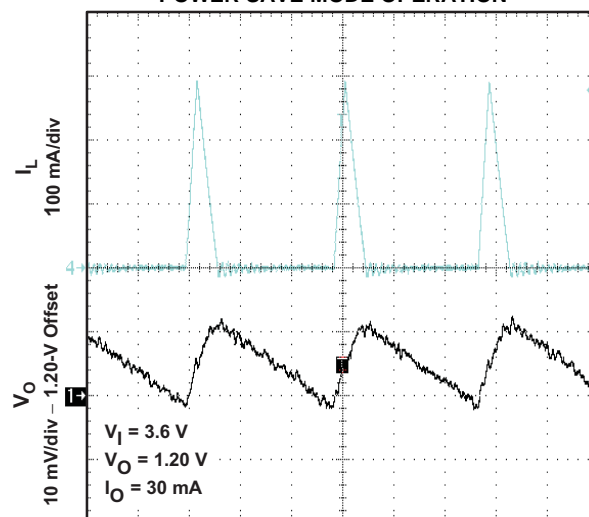
## TYPICAL CHARACTERISTICS (continued)

### PWM OPERATION



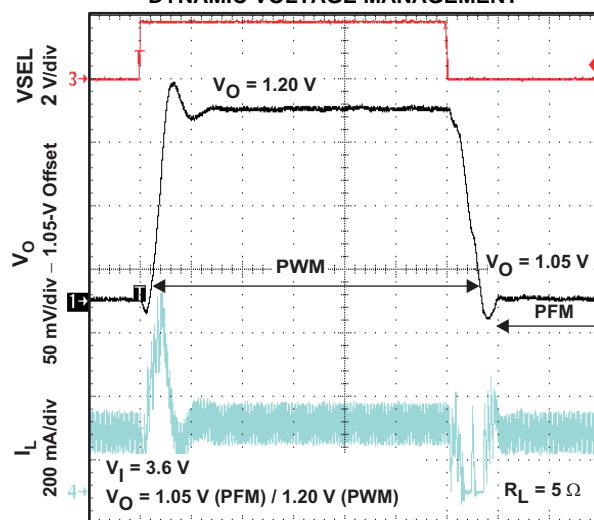
t - Time = 40 ns/div  
Figure 41.

### POWER SAVE MODE OPERATION



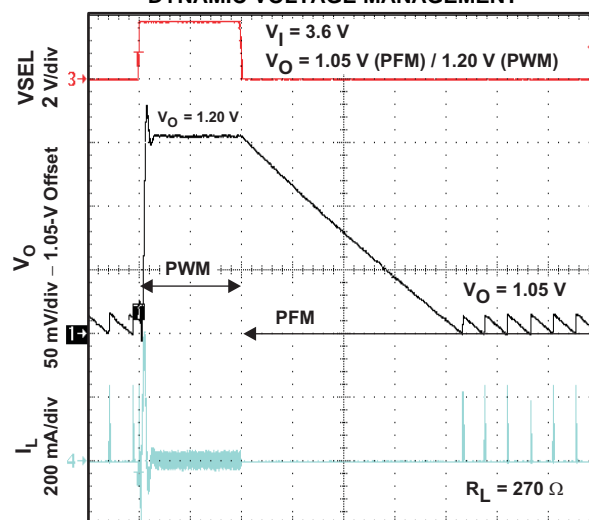
t - Time = 500 ns/div  
Figure 42.

### DYNAMIC VOLTAGE MANAGEMENT



t - Time = 5  $\mu$ s/div  
Figure 43.

### DYNAMIC VOLTAGE MANAGEMENT



t - Time = 25  $\mu$ s/div  
Figure 44.

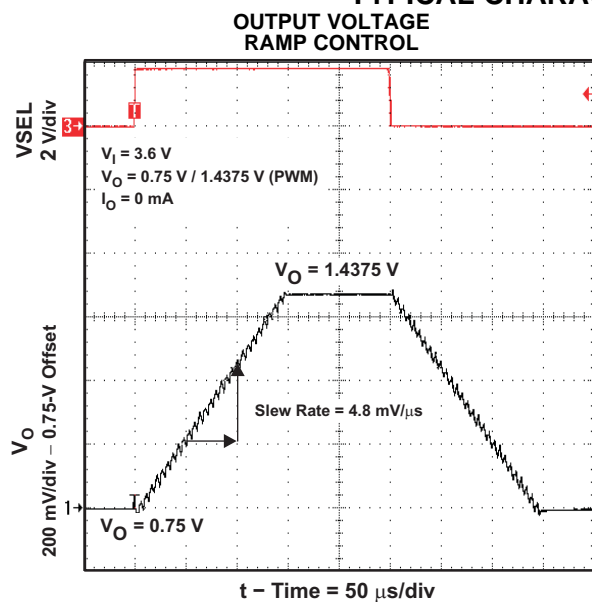
**TYPICAL CHARACTERISTICS (continued)**

Figure 45.

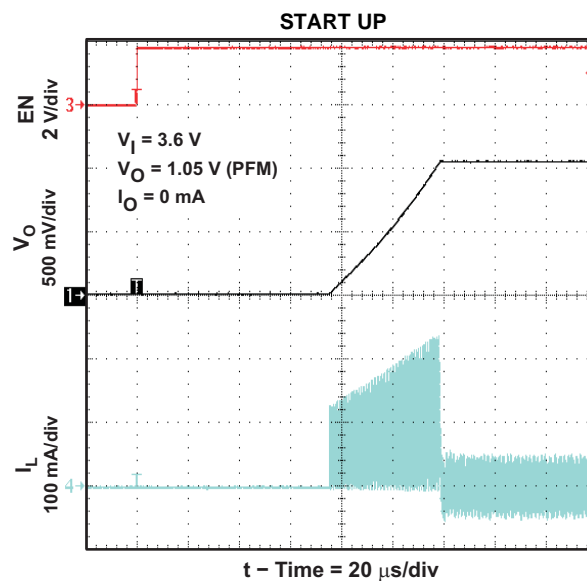


Figure 46.

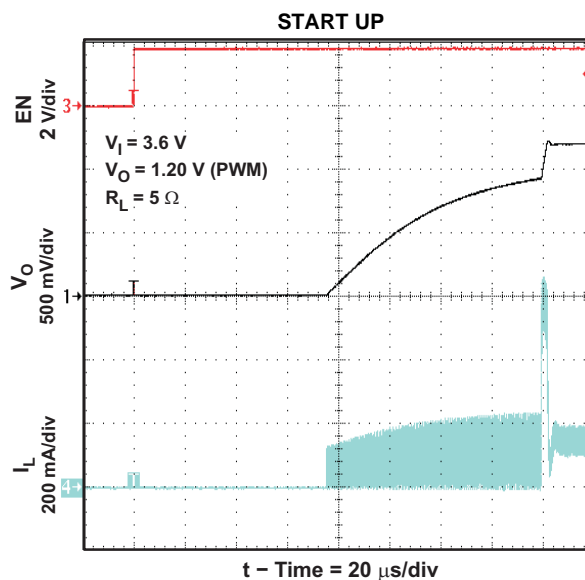


Figure 47.

## DETAILED DESCRIPTION

### Operation

The TPS62650-Q1 is a synchronous step-down converter typically operates at a regulated 6-MHz frequency pulse width modulation (PWM) at moderate to heavy load currents. At light load currents, the TPS62650-Q1 converter operates in power-save mode with pulse frequency modulation (PFM) and automatic transition into PWM operation when the load current increases.

The TPS62650-Q1 integrates an I<sup>2</sup>C compatible interface allowing transfers up to 3.4 Mbps. This communication interface can be used for dynamic voltage scaling with voltage steps down to 12.5 mV, for reprogramming the mode of operation (PFM or forced PWM) or disable/enabling the output voltage for instance. For more details, see the I<sup>2</sup>C interface and register description section.

The converter uses a unique frequency locked ring oscillating modulator to achieve *best-in-class* load and line response and allows the use of tiny inductors and small ceramic input and output capacitors. At the beginning of each switching cycle, the P-channel MOSFET switch is turned on and the inductor current ramps up rising the output voltage until the main comparator trips, then the control logic turns off the switch.

One key advantage of the non-linear architecture is that there is no traditional feed-back loop. The loop response to change in  $V_O$  is essentially instantaneous, which explains its extraordinary transient response. The absence of a traditional, high-gain compensated linear loop means that the TPS62650-Q1 is inherently stable over a range of small L and  $C_O$ .

Although this type of operation normally results in a switching frequency that varies with input voltage and load current, an internal frequency lock loop (FLL) holds the switching frequency constant over a large range of operating conditions.

Combined with *best in class* load and line transient response characteristics, the low quiescent current of the device (ca. 38 $\mu$ A) allows to maintain high efficiency at light load, while preserving fast transient response for applications requiring tight output regulation.

### SWITCHING FREQUENCY

The magnitude of the internal ramp, which is generated from the duty cycle, reduces for duty cycles either set of 50%. Thus, there is less overdrive on the main comparator inputs which tends to slow the conversion down. The intrinsic maximum operating frequency of the converter is about 10MHz to 12MHz, which is controlled to circa. 6MHz by a frequency locked loop.

When high or low duty cycles are encountered, the loop runs out of range and the conversion frequency falls below 6MHz. The tendency is for the converter to operate more towards a "constant inductor peak current" rather than a "constant frequency". In addition to this behavior which is observed at high duty cycles, it is also noted at low duty cycles.

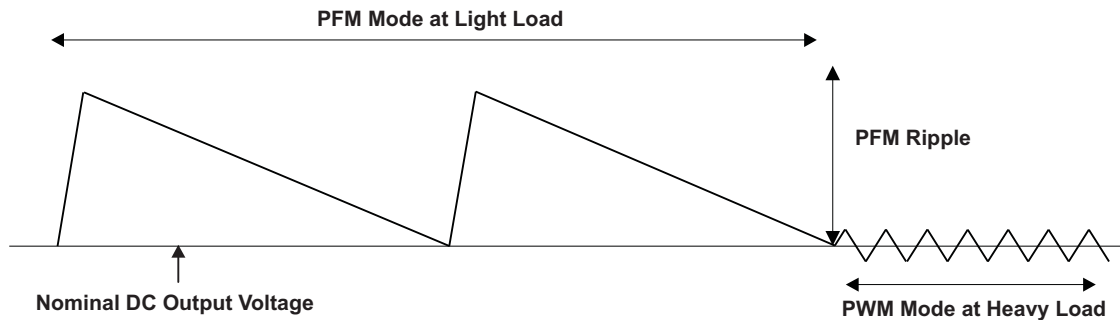
When the converter is required to operate towards the 6MHz nominal at extreme duty cycles, the application can be assisted by decreasing the ratio of inductance (L) to the output capacitor's equivalent serial inductance (ESL). This increases the *ESL step* seen at the main comparator's feed-back input thus decreasing its propagation delay, hence increasing the switching frequency.

### POWER-SAVE MODE

If the load current decreases, the converter will enter Power Save Mode operation automatically. During power-save mode the converter operates in discontinuous current (DCM) single-pulse PFM mode, which produces low output ripple compared with other PFM architectures.

When in power-save mode, the converter resumes its operation when the output voltage trips below the nominal voltage. It ramps up the output voltage with a minimum of one pulse and goes into power-save mode when the inductor current has returned to a zero steady state. The PFN on-time varies inversely proportional to the input voltage and proportional to the output voltage giving the regulated switching frequency when is steady-state.

PFM mode is left and PWM operation is entered as the output current can no longer be supported in PFM mode. As a consequence, the DC output voltage is typically positioned ca 0.5% above the nominal output voltage and the transition between PFM and PWM is seamless.



**Figure 48. Operation in PFM Mode and Transfer to PWM Mode**

## MODE SELECTION

Depending on the settings of CONTROL1 register the device can be operated in either the regulated frequency PWM mode or in the automatic PWM and power-save mode. In this mode, the converter operates in a regulated frequency PWM mode at moderate to heavy loads and in the PFM mode during light loads, which maintains high efficiency over a wide load current range. For more details, see the [CONTROL1](#) register description.

The regulated frequency PWM mode has the tightest regulation and the best line/load transient performance. Furthermore, this mode of operation allows simple filtering of the switching frequency for noise-sensitive applications. In forced PWM mode, the efficiency is lower compared to the power-save mode during light loads.

It is possible to switch from power-save mode (PFM) to forced PWM mode during operation either via the VSEL signal or by re-programming the [CONTROL1](#) register. This allows adjustments to the converters operation to match the specific system requirements leading to more efficient and flexible power management.

## ENABLE

The device starts operation when EN pin is set high and starts up with the soft start. This signal is gated by the EN\_DCDC bit defined in register VSEL0 and VSEL1. On rising edge of the EN pin, all the registers are reset with their default values. Enabling the converter's operation via the EN\_DCDC bit does not affect internal register settings. This allows the output voltage to be programmed to other values than the default voltage before starting up the converter. For more details, see the [VSEL0/1](#) register description.

Pulling the EN pin, VSEL0[6] bit or VSEL1[6] bit low forces the device into shutdown, with a shutdown current as defined in the electrical characteristics table. In this mode, the P and N-channel MOSFETs are turned off, the internal resistor feedback divider is disconnected, and the entire internal-control circuitry is switched off. For proper operation, the EN pin must be terminated and must not be left floating.

In addition, depending on the setting of CONTROL2[6] bit, the device can actively discharge the output capacitor when it turns off. The integrated discharge resistor has a typical resistance of 15  $\Omega$ . The required time to discharge the output capacitor at  $V_O$  depends on load current and the output capacitance value.

## SOFT START

The TPS62650-Q1 has an internal soft-start circuit that limits the inrush current during start-up. This limits input voltage drops when a battery or a high-impedance power source is connected to the input of the converter.

The soft-start system progressively increases the on-time from a minimum pulse-width of 35ns as a function of the output voltage. This mode of operation continues for c.a. 100 $\mu$ s after enable. Should the output voltage not have reached its target value by this time, such as in the case of heavy load, the soft-start transitions to a second mode of operation.

The converter will then operate in a current limit mode, specifically the P-MOS current limit is set to half the nominal limit and the N-channel MOSET remains on until the inductor current has reset. After a further 100  $\mu$ s, the device ramps up to full current limit operation providing that the output voltage has risen above 0.5V (approximately). Therefore, the start-up time depends on the output capacitor and load current.

## UNDERVOLTAGE LOCKOUT

The undervoltage lockout circuit prevents the device from misoperation at low input voltages. It prevents the converter from turning on the switch or rectifier MOSFET under undefined conditions. The TPS62650-Q1 device have a UVLO threshold set to 2.05V (typical). Fully functional operation is permitted down to 2.15 V input voltage.

## SHORT-CIRCUIT PROTECTION

The TPS62650-Q1 integrates a P-channel MOSFET current limit to protect the device against heavy load or short circuits. When the current in the P-channel MOSFET reaches its current limit, the P-channel MOSFET is turned off and the N-channel MOSFET is turned on. The regulator continues to limit the current on a cycle-by-cycle basis.

As soon as the output voltage falls below ca. 0.4V, the converter current limit is reduced to half of the nominal value and the PWROK bit is reset. Because the short-circuit protection is enabled during start-up, the device does not deliver more than half of its nominal current limit until the output voltage exceeds approximately 0.5V. This needs to be considered when a load acting as a current sink is connected to the output of the converter.

## THERMAL SHUTDOWN

As soon as the junction temperature,  $T_J$ , exceeds typically 140°C, the device goes into thermal shutdown. In this mode, the P- and N-channel MOSFETs are turned off. The device continues its operation when the junction temperature again falls below typically 130°C.

## VOLTAGE AND MODE SELECTION

The TPS62650-Q1 features a pin-selectable output voltage. VSEL is primarily used to scale the output voltage between active (VSEL = HIGH) and sleep mode (VSEL = LOW). For maximum flexibility, it is possible to reprogram the operating mode of the converter (e.g. forced PWM, or auto transition PFM/PWM) associated with VSEL signal via the I<sup>2</sup>C interface

VSEL output voltage and mode selection is defined as following:

**VSEL = LOW:** — DC/DC output voltage determined by VSEL0 register value. DC/DC mode of operation is determined by MODE0 bit in [CONTROL1](#) register.

**VSEL = HIGH:** — DC/DC output voltage determined by VSEL1 register value. DC/DC mode of operation is determined by MODE1 bit in [CONTROL1](#) register.

The application processor programs via I<sup>2</sup>C the output voltages associated with the two states of VSEL signal: floor (VSEL0) and roof (VSEL1) values. The application processor also writes the DEFSLEW value in the CONTROL2 register to control the output voltage ramp rate.

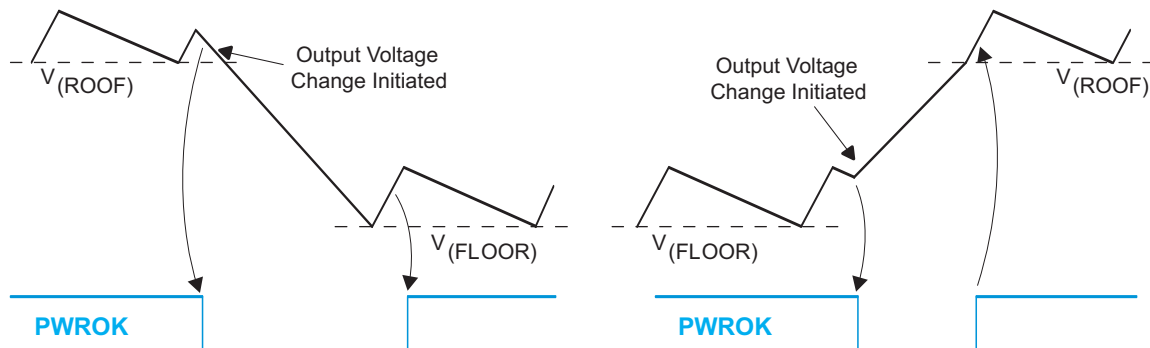
These two registers can be continuously updated via I<sup>2</sup>C to provide the appropriate output voltage according to the VSEL input. The voltage changes with the selected ramp rate immediately after writing to the VSEL0 or VSEL1 register.

[Table 1](#) shows the output voltage states depending on VSEL0, VSEL1 registers, and VSEL signal.

**Table 1. Dynamic Voltage Scaling Functional Overview**

VSEL PIN	VSEL0 REGISTER	VSEL1 REGISTER	OUTPUT VOLTAGE
Low	No action	No action	Floor
Low	Write new value	No action	Change to new value
Low	No action	Write	No change stays at floor voltage
High	No action	No action	Roof
High	Write new value	No action	No change stays at roof voltage
High	No action	Write new value	Change to new value

In PFM mode, when the output voltage is programmed to a lower value by toggling VSEL signal from high to low, PWROK is defined as low, while the output capacitor is discharged by the load until the converter starts pulsing to maintain the voltage within regulation. In multiple-step mode, PWROK is defined as low while the output voltage is ramping up or down.



**Figure 49. PWROK Functional Behavior**

### VOLTAGE RAMP CONTROL

The TPS62650-Q1 offers a voltage ramp rate control that can operate in two different modes:

- Multiple-Step Mode
- Single-Step Mode

The mode is selected via DEFSLEW control bits in the CONTROL2 register.

#### Single-Step Voltage Scaling Mode (default), DEFSLEW[2:0] = [111]

In single-step mode, the TPS62650-Q1 ramps the output voltage with maximum slew-rate when transitioning between the floor and the roof voltages (switch to a higher voltage).

When switching between the roof and the floor voltages (transition to a lower voltage), the ramp rate control is dependent on the mode selection (see [CONTROL1](#) register) associated with the target register (Forced PWM or auto transition PFM/PWM).

[Table 2](#) shows the ramp rate control when transitioning to a lower voltage with DEFSLEW set to immediate transition.

**Table 2. Ramp Rate Control vs. Target Mode**

Mode Associated with Target Voltage	Output Voltage Ramp Rate
Forced PWM	Immediate
PFM/PWM	DC/DC converter stops switching. Time to ramp down depends on output capacitance and load current

For instance, when the output is programmed to transition to a lower voltage with PFM operation enabled, the TPS62650-Q1 ramps down the output voltage without controlling the ramp rate or having intermediate micro-steps. The required time to ramp down the voltage depends on the capacitance present at the output of the TPS62650-Q1 and on the load current. From an overall system perspective, this is the most efficient way to perform dynamic voltage scaling.

#### Multiple-Step Voltage Scaling Mode, DEFSLEW[2:0] = [000] to [110]

In multiple-step mode the TPS62650-Q1 controls the output voltage ramp rate regardless of the load current and mode of operation (e.g. Forced PWM or PFM/PWM). The voltage ramp control is done by adjusting the time between the voltage micro-steps.



## THEORY OF OPERATION

### Serial Interface Description

I<sup>2</sup>C is a 2-wire serial interface developed by Philips Semiconductor (see I<sup>2</sup>C-Bus Specification, Version 2.1, January 2000). The bus consists of a data line (SDA) and a clock line (SCL) with pull-up structures. When the bus is idle, both SDA and SCL lines are pulled high. All the I<sup>2</sup>C compatible devices connect to the I<sup>2</sup>C bus through open drain I/O pins, SDA and SCL. A master device, usually a microcontroller or a digital signal processor, controls the bus. The master is responsible for generating the SCL signal and device addresses. The master also generates specific conditions that indicate the START and STOP of data transfer. A slave device receives and/or transmits data on the bus under control of the master device.

The TPS62650-Q1 device works as a slave and supports the following data transfer modes, as defined in the I<sup>2</sup>C-Bus Specification: standard mode (100 kbps), fast mode (400 kbps), fast mode plus (1 Mbps) and high-speed mode (up to 3.4 Mbps). The interface adds flexibility to the power supply solution, enabling most functions to be programmed to new values depending on the instantaneous application requirements. Register contents remain intact as long as supply voltage remains above 2.1 V (typical).

The data transfer protocol for standard, fast and fast plus modes is exactly the same, therefore, they are referred to as F/S-mode in this document. The protocol for high-speed mode is different from the F/S-mode, and it is referred to as HS-mode. The TPS62650-Q1 device supports 7-bit addressing; 10-bit addressing and general call address are not supported.

The TPS62650-Q1 device has a 7-bit address with two bits factory programmable allowing up to four dc/dc converters to be connected to the same bus. The 4 MSBs are 1001 and the LSB is 0.

### Standard-, Fast- and Fast-Mode Plus Protocol

The *master* initiates data transfer by generating a start condition. The start condition is when a high-to-low transition occurs on the SDA line while SCL is high, see [Figure 50](#). All I<sup>2</sup>C-compatible devices should recognize a start condition.

The master then generates the SCL pulses, and transmits the 7-bit address and the read/write direction bit R/W on the SDA line. During all transmissions, the master ensures that data is *valid*. A valid data condition requires the SDA line to be stable during the entire high period of the clock pulse, see [Figure 51](#). All devices recognize the address sent by the master and compare it to their internal fixed addresses. Only the slave device with a matching address generates an *acknowledge*, see [Figure 52](#), by pulling the SDA line low during the entire high period of the ninth SCL cycle. Upon detecting this acknowledge, the master knows that the communication link with a slave has been established.

The master generates further SCL cycles to either transmit data to the slave (R/W bit 1) or receive data from the slave (R/W bit 0). In either case, the receiver needs to acknowledge the data sent by the transmitter. An acknowledge signal can either be generated by the master or by the slave, depending on which one is the receiver. 9-bit valid data sequences consisting of 8-bit data and 1-bit acknowledge can continue as long as necessary.

To signal the end of the data transfer, the master generates a stop condition by pulling the SDA line from low to high while the SCL line is high, see [Figure 50](#). This releases the bus and stops the communication link with the addressed slave. All I<sup>2</sup>C compatible devices must recognize the stop condition. Upon the receipt of a stop condition, all devices know that the bus is released, and they wait for a start condition followed by a matching address.

Attempting to read data from register addresses not listed in this section results in 00h being read out.

## H/S-Mode Protocol

When the bus is idle, both SDA and SCL lines are pulled high by the pull-up devices.

The master generates a start condition followed by a valid serial byte containing HS master code 00001XXX. This transmission is made in F/S-mode at no more than 400 Kbps. No device is allowed to acknowledge the HS master code, but all devices must recognize it and switch their internal setting to support 3.4-Mbps operation.

The master then generates a repeated start condition (a repeated start condition has the same timing as the start condition). After this repeated start condition, the protocol is the same as F/S-mode, except that transmission speeds up to 3.4 Mbps are allowed. A stop condition ends the HS-mode and switches all the internal settings of the slave devices to support the F/S-mode. Instead of using a stop condition, repeated start conditions are used to secure the bus in HS-mode.

Attempting to read data from register addresses not listed in this section results in FFh being read out.

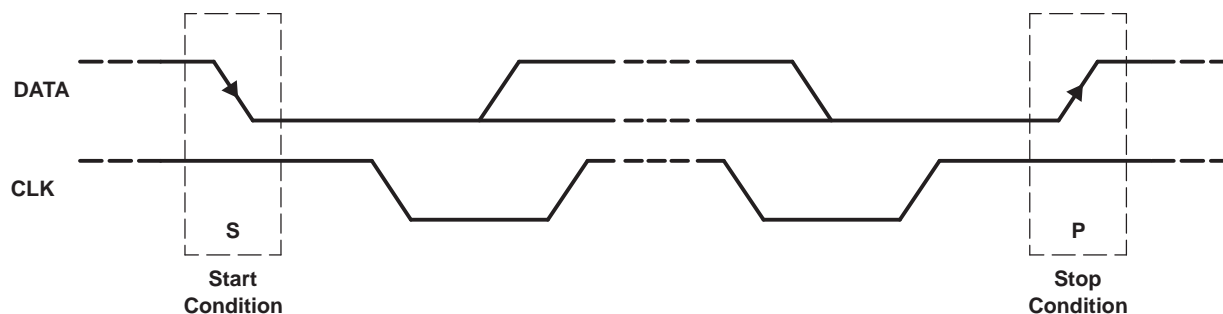


Figure 50. START and STOP Conditions

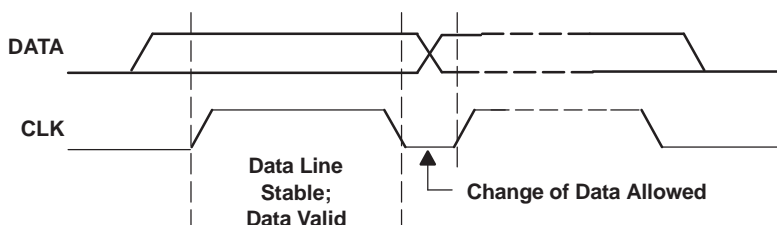


Figure 51. Bit Transfer on the Serial Interface

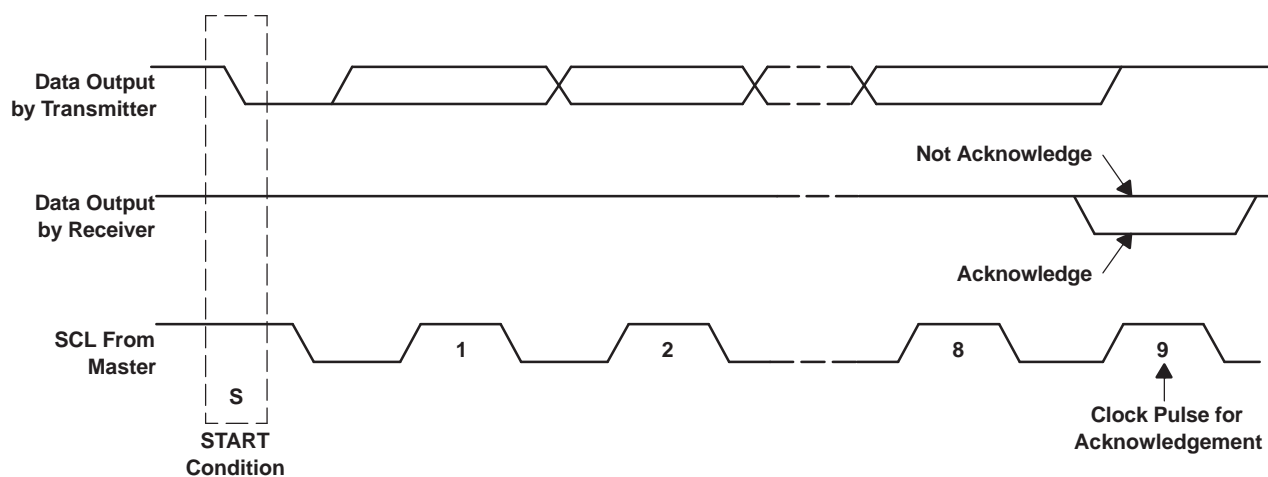


Figure 52. Acknowledge on the I<sup>2</sup>C Bus

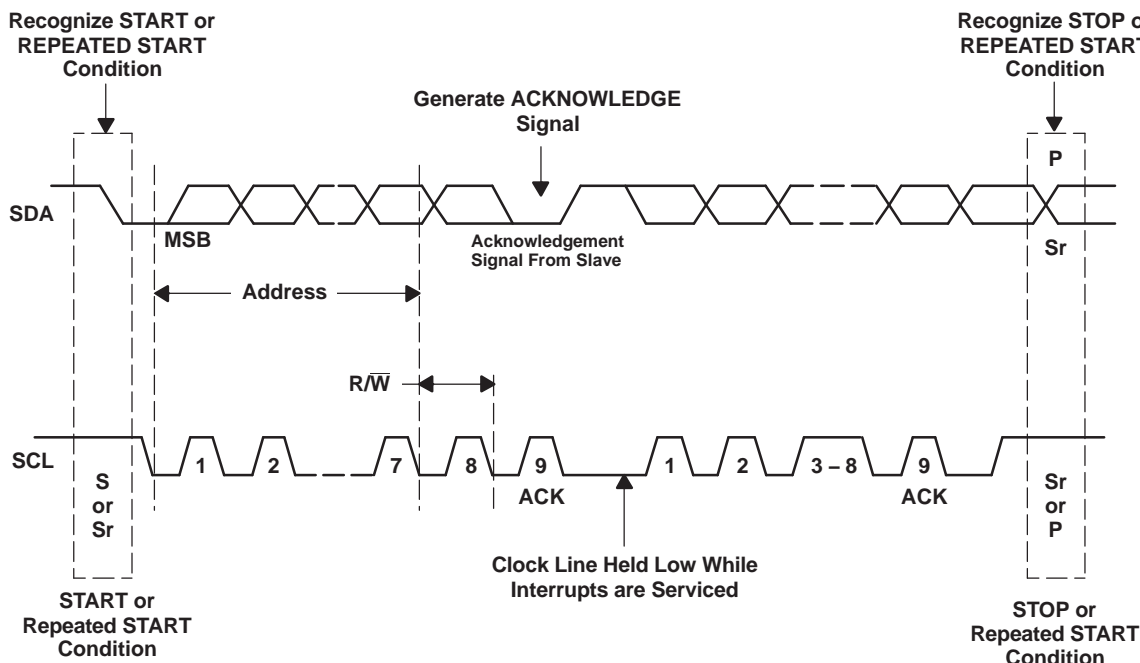


Figure 53. Bus Protocol

### TPS62650-Q1 I<sup>2</sup>C Update Sequence

The TPS62650-Q1 requires a start condition, a valid I<sup>2</sup>C address, a register address byte, and a data byte for a single update. After the receipt of each byte, TPS62650-Q1 device acknowledges by pulling the SDA line low during the high period of a single clock pulse. A valid I<sup>2</sup>C address selects the TPS62650-Q1. TPS62650-Q1 performs an update on the falling edge of the LSB byte.

When the TPS62650-Q1 is in hardware shutdown (EN pin tied to ground) the device can not be updated via the I<sup>2</sup>C interface. Conversely, the I<sup>2</sup>C interface is fully functional during software shutdown (EN\_DCDC bit = 0).

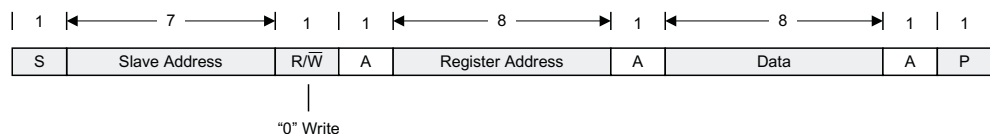


Figure 54. "Write" Data Transfer Format in Standard, Fast- and Fast-Plus Modes

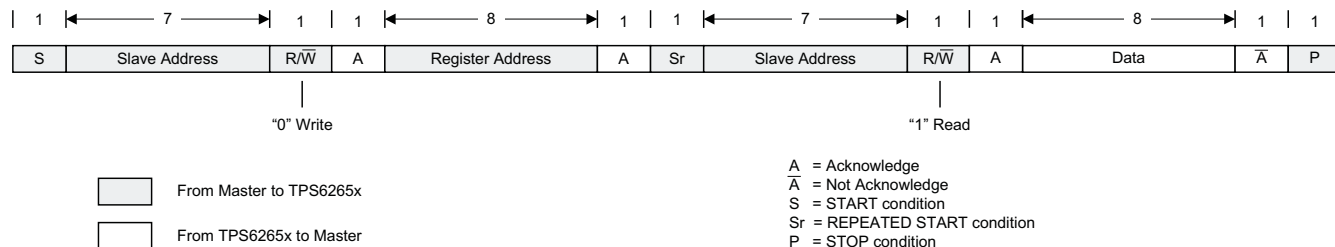


Figure 55. "Read" Data Transfer Format in Standard, Fast- and Fast-Plus Modes

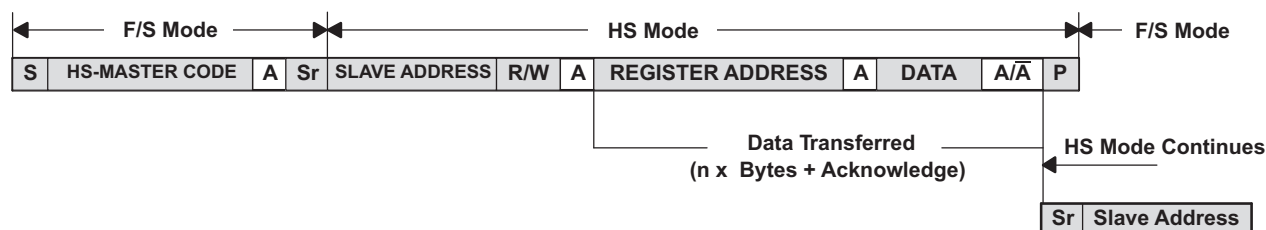


Figure 56. Data Transfer Format in H/S-Mode

**Slave Address Byte**

MSB							LSB
X	1	0	0	1	A2	A1	0

The slave address byte is the first byte received following the START condition from the master device. The first four bits (MSBs) of the address are factory preset to 1001. The next two bits (A2, A1) of the address are device option dependent. The LSB bit (A0) is also factory preset to 0. Up to 4 TPS62650-Q1 type of devices can be connected to the same I<sup>2</sup>C-Bus. See the ordering information table for more details.

**Register Address Byte**

MSB							LSB
0	0	0	0	0	0	D1	D0

Following the successful acknowledgment of the slave address, the bus master sends a byte to the TPS62650-Q1, which contains the address of the register to be accessed. The TPS62650-Q1 contains four 8-bit registers accessible via a bidirectional I<sup>2</sup>C-bus interface. All internal registers have read and write access.

## REGISTER DESCRIPTION

### VSEL0 REGISTER DESCRIPTION

Memory location: 0x00

Description	EN_DCDC	FREE	VSM0[5:0]					
Bits	D7	D6	D5	D4	D3	D2	D1	D0
Memory type	R/W	R/W	R/W	R/W	R/W	R/W	R/W	R/W
Default value	1	0	X	X	X	X	X	X

Bit	Description
EN_DCDC	<b>Enable/Disable DC/DC operation.</b> This bit gates the external EN pin control signal. This bit is mirrored in VSEL1 register. 0: Device in shutdown regardless of the EN signal. 1: Device enabled when EN is high, disabled when EN is low.
VSM0[5:0]	<b>Output voltage selection bits (floor voltage).<sup>(1)</sup></b> 6-bit unsigned binary linear coding. Output voltage = Minimum output voltage + (VSM0[5:0] x 12.5 mV)

(1) Register value is set according to the default output voltage, see ordering information table.

### VSEL1 REGISTER DESCRIPTION

Memory location: 0x01

Description	EN_DCDC	FREE	VSM1[5:0]					
Bits	D7	D6	D5	D4	D3	D2	D1	D0
Memory type	R/W	R/W	R/W	R/W	R/W	R/W	R/W	R/W
Default value	1	0	X	X	X	X	X	X

Bit	Description
EN_DCDC	<b>Enable/Disable DC/DC operation.</b> This bit gates the external EN pin control signal. This bit is mirrored in VSEL0 register. 0: Device in shutdown regardless of the EN signal. 1: Device enabled when EN is high, disabled when EN is low.
VSM1[5:0]	<b>Output voltage selection bits (roof voltage).<sup>(1)</sup></b> 6-bit unsigned binary linear coding. Output voltage = Minimum output voltage + (VSM1[5:0] x 12.5 mV)

(1) Register value is set according to the default output voltage, see ordering information table.

## CONTROL1 REGISTER DESCRIPTION

Memory location: 0x02

Description	RESERVED	RESERVED	FREE	FREE	MODE_CTRL[1:0]		MODE1	MODE0
Bits	D7	D6	D5	D4	D3	D2	D1	D0
Memory type	R	R	R/W	R/W	R/W	R/W	R/W	R/W
Default value	0	0	0	0	0	0	0	0

Bit	Description
<b>MODE_CTRL[1:0]</b>	<b>Mode control bits.<sup>(1)</sup></b> 00: Operation follows MODE0, MODE1. 01: PFM/PWM operation independent of VSEL signal. 10: Forced PWM operation independent of VSEL signal. 11: PFM/PWM operation independent of VSEL signal.
<b>MODE1</b>	<b>VSEL high (roof voltage) operating mode selection bit.</b> 0: Forced PWM. 1: PFM/PWM automatic transition.
<b>MODE0</b>	<b>VSEL low (floor voltage) operating mode selection bit.</b> 0,1: PFM/PWM automatic transition (no effect).

(1) See the ordering information table to verify the validity of this option.

## CONTROL2 REGISTER DESCRIPTION

Memory location: 0x03

Description	FREE	OUTPUT_DISCHARGE	PWROK	FREE	FREE	DEFSLEW		
Bits	D7	D6	D5	D4	D3	D2	D1	D0
Memory type	R/W	R/W	R/W	R/W	R/W	R/W	R/W	R/W
Default value	0	1	0	0	0	1	1	1

Bit	Description
<b>OUTPUT_DISCHARGE</b>	<b>Output capacitor auto-discharge control bit.</b> 0: The output capacitor is not actively discharged when the converter is disabled. 1: The output capacitor is discharged through an internal resistor when the converter is disabled.
<b>PWROK</b>	<b>Power good bit.</b> 0: The output voltage is not within its regulation limits. 1: The output voltage is in regulation.
<b>DEFSLEW</b>	<b>Output voltage slew-rate control bits.</b> 000: 0.15mV/μs 001: 0.3mV/μs 010: 0.6mV/μs 011: 1.2mV/μs 100: 2.4mV/μs 101: 4.8mV/μs 110: 9.6mV/μs 111: Immediate

## APPLICATION INFORMATION

### INDUCTOR SELECTION

The TPS62650-Q1 series of step-down converters have been optimized to operate with an effective inductance value in the range of 0.3μH to 1.3μH and with output capacitors in the range of 4.7μF to 10μF. The internal compensation is optimized to operate with an output filter of L = 0.47μH and C<sub>O</sub> = 4.7μF. Larger or smaller inductor values can be used to optimize the performance of the device for specific operation conditions. For more details, refer to the section "checking loop stability".

The inductor value affects its peak-to-peak ripple current, the PWM-to-PFM transition point, the output voltage ripple and the efficiency. The selected inductor has to be rated for its dc resistance and saturation current. The inductor ripple current (ΔI<sub>L</sub>) decreases with higher inductance and increases with higher V<sub>I</sub> or V<sub>O</sub>.

$$\Delta I_L = \frac{V_O}{V_I} \times \frac{V_I - V_O}{L \times f_{SW}} \quad \Delta I_{L(MAX)} = I_{O(MAX)} + \frac{\Delta I_L}{2}$$

with: f<sub>SW</sub> = switching frequency (6 MHz typical)

L = inductor value

ΔI<sub>L</sub> = peak-to-peak inductor ripple current

I<sub>L(MAX)</sub> = maximum inductor current (1)

In high-frequency converter applications, the efficiency is essentially affected by the inductor AC resistance (i.e. quality factor) and to a smaller extent by the inductor DCR value. To achieve high efficiency operation, care should be taken in selecting inductors featuring a quality factor above 25 at the switching frequency. Increasing the inductor value produces lower RMS currents, but degrades transient response. For a given physical inductor size, increased inductance usually results in an inductor with lower saturation current.

The total losses of the coil consist of both the losses in the DC resistance (R<sub>(DC)</sub>) and the following frequency-dependent components:

- The losses in the core material (magnetic hysteresis loss, especially at high switching frequencies)
- Additional losses in the conductor from the skin effect (current displacement at high frequencies)
- Magnetic field losses of the neighboring windings (proximity effect)
- Radiation losses

The following inductor series from different suppliers have been used with the TPS62650-Q1 converters.

**Table 3. List of Inductors**

MANUFACTURER	SERIES	DIMENSIONS
MURATA	LQM21PN1R0NGR	2.0 x 1.2 x 1.0 max. height
	LQM21PNR54MG0	2.0 x 1.2 x 1.0 max. height
	LQM21PNR47MG0	2.0 x 1.2 x 1.0 max. height
	LQM2MPN1R0NG0	2.0 x 1.6 x 1.0 max. height
TOKO	MDT2012-CX1R0A	2.0 x 1.2 x 1.0 max. height
FDK	MIPS2012D1R0-X2	2.0 x 1.2 x 1.0 max. height

## OUTPUT CAPACITOR SELECTION

The advanced fast-response voltage mode control scheme of the TPS62650-Q1 allows the use of tiny ceramic capacitors. Ceramic capacitors with low ESR values have the lowest output voltage ripple and are recommended. For best performance, the device should be operated with a minimum effective output capacitance of 1.6 $\mu$ F. The output capacitor requires either an X7R or X5R dielectric. Y5V and Z5U dielectric capacitors, aside from their wide variation in capacitance over temperature, become resistive at high frequencies.

At nominal load current, the device operates in PWM mode and the overall output voltage ripple is the sum of the voltage step caused by the output capacitor ESL and the ripple current flowing through the output capacitor impedance.

At light loads, the output capacitor limits the output ripple voltage and provides holdup during large load transitions. A 4.7 $\mu$ F capacitor typically provides sufficient bulk capacitance to stabilize the output during large load transitions. The typical output voltage ripple is 1.5% of the nominal output voltage  $V_O$ .

The output voltage ripple during PFM mode operation can be kept small. The PFM pulse is time controlled, which allows to modify the charge transferred to the output capacitor by the value of the inductor. The resulting PFM output voltage ripple and PFM frequency depend in first order on the size of the output capacitor and the inductor value. The PFM frequency decreases with smaller inductor values and increases with larger once. Increasing the output capacitor value and the effective inductance will minimize the output ripple voltage.

## INPUT CAPACITOR SELECTION

Because of the nature of the buck converter having a pulsating input current, a low ESR input capacitor is required to prevent large voltage transients that can cause misbehavior of the device or interferences with other circuits in the system. For most applications, a 2.2 $\mu$ F or 4.7 $\mu$ F capacitor is sufficient. If the application exhibits a noisy or erratic switching frequency, the remedy will probably be found by experimenting with the value of the input capacitor.

Take care when using only ceramic input capacitors. When a ceramic capacitor is used at the input and the power is being supplied through long wires, such as from a wall adapter, a load step at the output can induce ringing at the VIN pin. This ringing can couple to the output and be mistaken as loop instability or could even damage the part. Additional "bulk" capacitance (electrolytic or tantalum) should in this circumstance be placed between  $C_I$  and the power source lead to reduce ringing than can occur between the inductance of the power source leads and  $C_I$ .

## CHECKING LOOP STABILITY

The first step of circuit and stability evaluation is to look from a steady-state perspective at the following signals:

- Switching node, SW
- Inductor current,  $I_L$
- Output ripple voltage,  $V_{O(AC)}$

These are the basic signals that need to be measured when evaluating a switching converter. When the switching waveform shows large duty cycle jitter or the output voltage or inductor current shows oscillations, the regulation loop may be unstable. This is often a result of board layout and/or L-C combination.

As a next step in the evaluation of the regulation loop, the load transient response is tested. The time between the application of the load transient and the turn on of the P-channel MOSFET, the output capacitor must supply all of the current required by the load.  $V_O$  immediately shifts by an amount equal to  $\Delta I_{(LOAD)} \times ESR$ , where ESR is the effective series resistance of  $C_O$ .  $\Delta I_{(LOAD)}$  begins to charge or discharge  $C_O$  generating a feedback error signal used by the regulator to return  $V_O$  to its steady-state value. The results are most easily interpreted when the device operates in PWM mode.

During this recovery time,  $V_O$  can be monitored for settling time, overshoot or ringing that helps judge the converter's stability. Without any ringing, the loop has usually more than 45° of phase margin.

Because the damping factor of the circuitry is directly related to several resistive parameters (e.g., MOSFET  $r_{DS(on)}$ ) that are temperature dependant, the loop stability analysis has to be done over the input voltage range, load current range, and temperature range.



## LAYOUT CONSIDERATIONS

As for all switching power supplies, the layout is an important step in the design. High-speed operation of the TPS62650-Q1 devices demand careful attention to PCB layout. Care must be taken in board layout to get the specified performance. If the layout is not carefully done, the regulator could show poor line and/or load regulation, stability and switching frequency issues as well as EMI problems. It is critical to provide a low inductance, impedance ground path. Therefore, use wide and short traces for the main current paths.

The input capacitor should be placed as close as possible to the IC pins as well as the inductor and output capacitor. In order to get an optimum *ESL step*, the output voltage feedback point (FB) should be taken in the output capacitor path, approximately 1mm away for it. The feed-back line should be routed away from noisy components and traces (e.g. SW line).

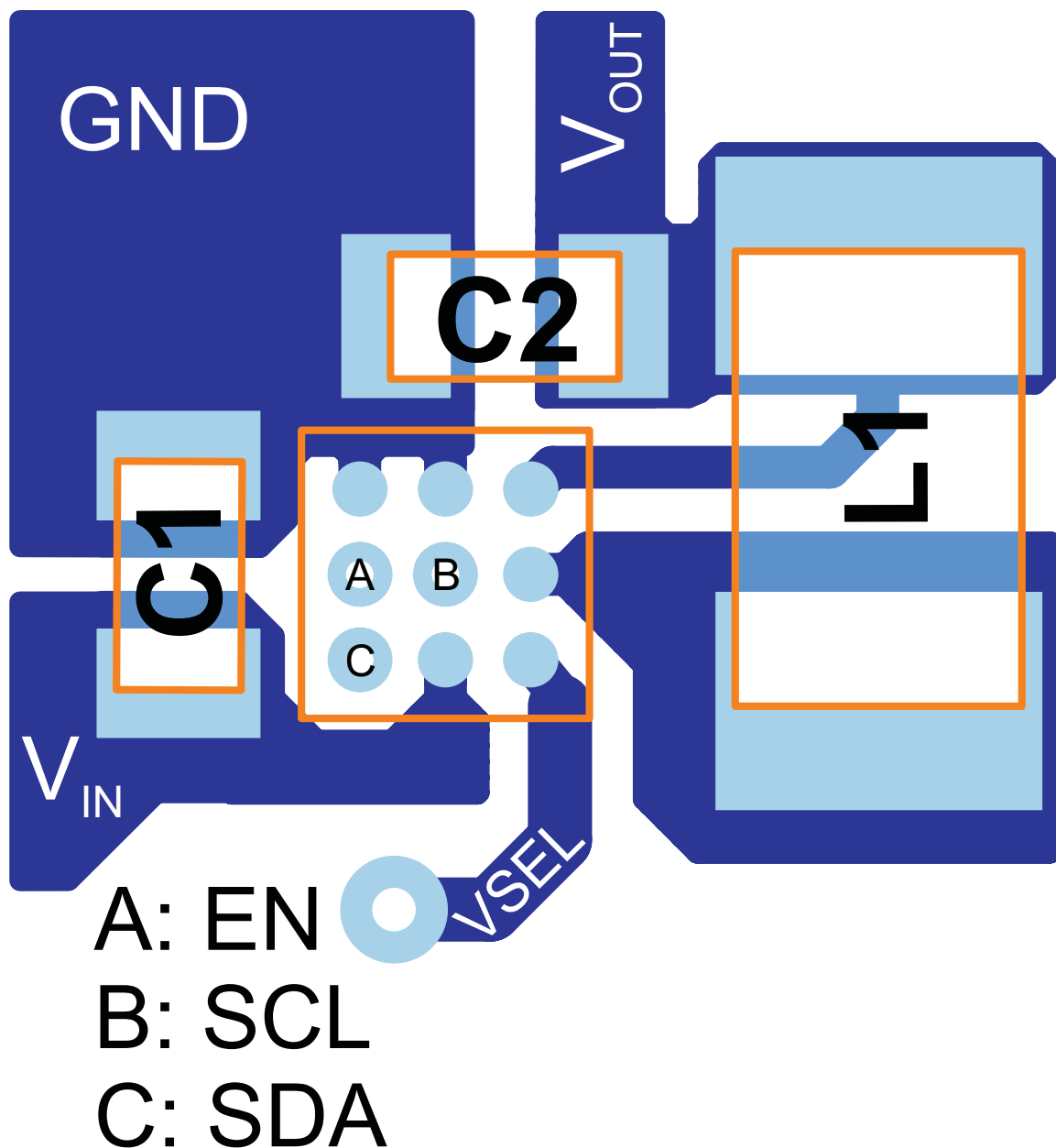


Figure 57. Suggested Layout (Top)

## Thermal Information

Implementation of integrated circuits in low-profile and fine-pitch surface-mount packages typically requires special attention to power dissipation. Many system-dependant issues such as thermal coupling, airflow, added heat sinks, and convection surfaces, and the presence of other heat-generating components, affect the power-dissipation limits of a given component.

Three basic approaches for enhancing thermal performance are listed below:

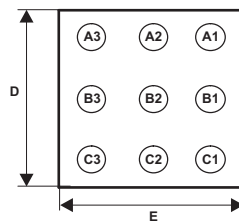
- Improving the power dissipation capability of the PCB design
- Improving the thermal coupling of the component to the PCB
- Introducing airflow in the system

The maximum recommended junction temperature ( $T_J$ ) of the TPS62650-Q1 device is 105°C. The thermal resistance of the 9-pin CSP package (YFF) is  $R_{\theta JA} = 105^\circ\text{C/W}$ . The regulator operation is specified to a maximum ambient temperature  $T_A$  of 105°C. Therefore, the maximum power dissipation is about 200mW.

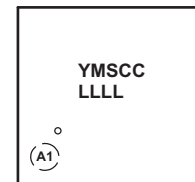
$$P_{D\text{MAX}} = \frac{T_{J\text{MAX}} - T_A}{R_{\theta JA}} = \frac{105^\circ\text{C} - 85^\circ\text{C}}{105^\circ\text{C/W}} = 190 \text{ mW} \quad (2)$$

## PACKAGE SUMMARY

**CHIP SCALE PACKAGE  
(BOTTOM VIEW)**



**CHIP SCALE PACKAGE  
(TOP VIEW)**



Code:

- YM - Year Month date code
- S - assembly site code
- CC - Chip code
- LLLL - Lot trace code

## REVISION HISTORY

### Changes from Revision A (March 2012) to Revision B

### Page

- 
- Changed " $T_A$ " to " $T_J$ " ..... [2](#)
-

## PACKAGING INFORMATION

Orderable part number	Status (1)	Material type (2)	Package   Pins	Package qty   Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
<a href="#">TPS62650TYFFRQ1</a>	Active	Production	DSBGA (YFF)   9	3000   LARGE T&R	Yes	SNAGCU	Level-1-260C-UNLIM	-40 to 105	Q1
TPS62650TYFFRQ1.A	Active	Production	DSBGA (YFF)   9	3000   LARGE T&R	Yes	SNAGCU	Level-1-260C-UNLIM	-40 to 105	Q1

<sup>(1)</sup> **Status:** For more details on status, see our [product life cycle](#).

<sup>(2)</sup> **Material type:** When designated, preproduction parts are prototypes/experimental devices, and are not yet approved or released for full production. Testing and final process, including without limitation quality assurance, reliability performance testing, and/or process qualification, may not yet be complete, and this item is subject to further changes or possible discontinuation. If available for ordering, purchases will be subject to an additional waiver at checkout, and are intended for early internal evaluation purposes only. These items are sold without warranties of any kind.

<sup>(3)</sup> **RoHS values:** Yes, No, RoHS Exempt. See the [TI RoHS Statement](#) for additional information and value definition.

<sup>(4)</sup> **Lead finish/Ball material:** Parts may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

<sup>(5)</sup> **MSL rating/Peak reflow:** The moisture sensitivity level ratings and peak solder (reflow) temperatures. In the event that a part has multiple moisture sensitivity ratings, only the lowest level per JEDEC standards is shown. Refer to the shipping label for the actual reflow temperature that will be used to mount the part to the printed circuit board.

<sup>(6)</sup> **Part marking:** There may be an additional marking, which relates to the logo, the lot trace code information, or the environmental category of the part.

Multiple part markings will be inside parentheses. Only one part marking contained in parentheses and separated by a "~" will appear on a part. If a line is indented then it is a continuation of the previous line and the two combined represent the entire part marking for that device.

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In no event shall TI's liability arising out of such information exceed the total purchase price of the TI part(s) at issue in this document sold by TI to Customer on an annual basis.

### OTHER QUALIFIED VERSIONS OF TPS62650-Q1 :

- Catalog : [TPS62650](#)

NOTE: Qualified Version Definitions:

- Catalog - TI's standard catalog product

## TAPE AND REEL INFORMATION



\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
TPS62650TYFFRQ1	DSBGA	YFF	9	3000	180.0	8.4	1.45	1.45	0.8	4.0	8.0	Q1

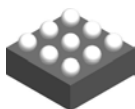
## TAPE AND REEL BOX DIMENSIONS



\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
TPS62650TYFFRQ1	DSBGA	YFF	9	3000	182.0	182.0	20.0

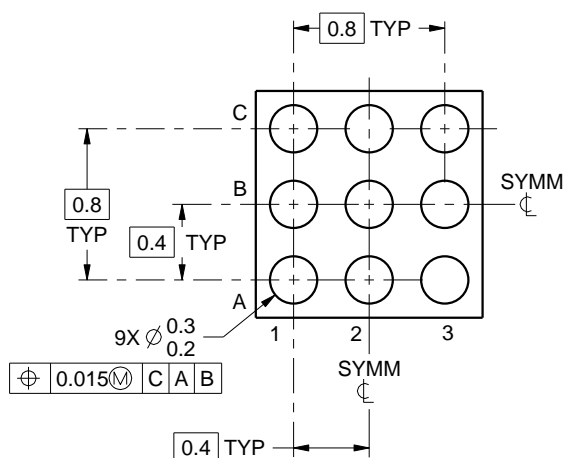
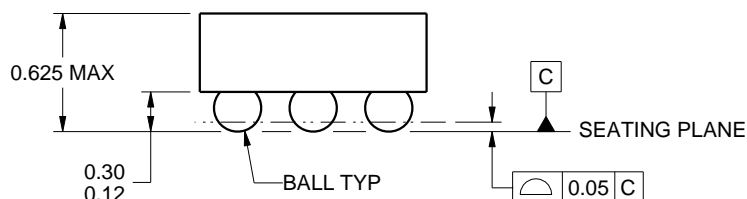
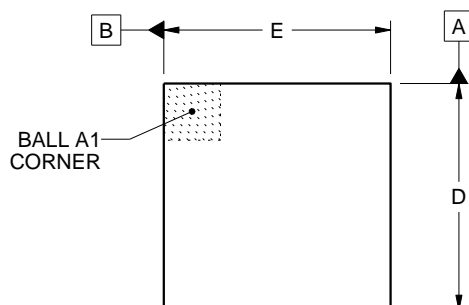
YFF0009



## PACKAGE OUTLINE

DSBGA - 0.625 mm max height

DIE SIZE BALL GRID ARRAY



4219552/A 05/2016

### NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.

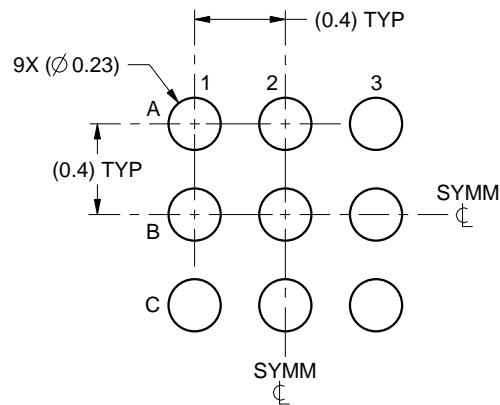


# EXAMPLE BOARD LAYOUT

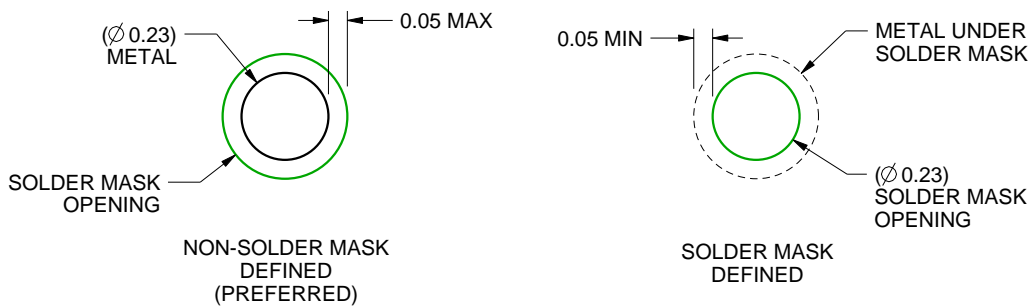
YFF0009

DSBGA - 0.625 mm max height

DIE SIZE BALL GRID ARRAY



LAND PATTERN EXAMPLE  
SCALE:30X



SOLDER MASK DETAILS  
NOT TO SCALE

4219552/A 05/2016

NOTES: (continued)

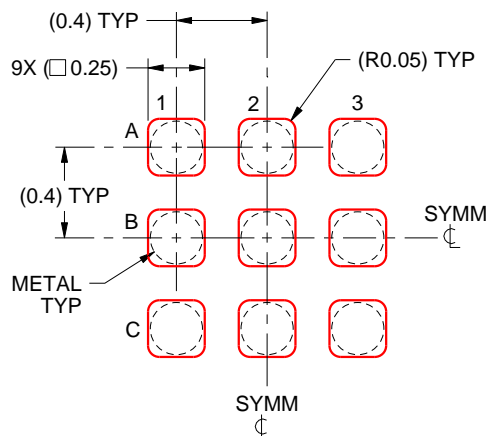
3. Final dimensions may vary due to manufacturing tolerance considerations and also routing constraints. For more information, see Texas Instruments literature number SNVA009 ([www.ti.com/lit/snva009](http://www.ti.com/lit/snva009)).

## EXAMPLE STENCIL DESIGN

YFF0009

DSBGA - 0.625 mm max height

DIE SIZE BALL GRID ARRAY



SOLDER PASTE EXAMPLE  
BASED ON 0.1 mm THICK STENCIL  
SCALE:30X

4219552/A 05/2016

NOTES: (continued)

4. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release.

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